RETURN TO CALIBRATION

INSTRUCTION MANUAL

MODEL 311/310

TRANSISTOR NOISE ANALYZER

For Serial No. 132

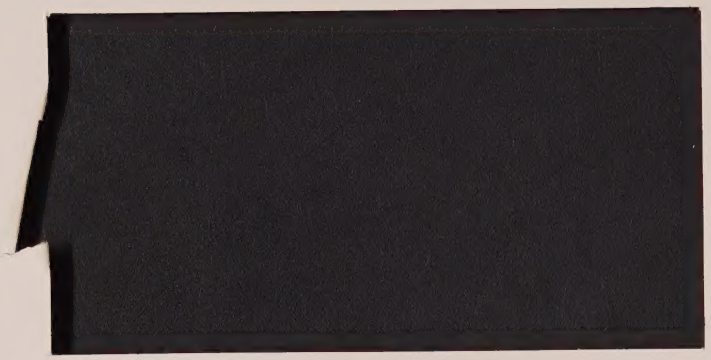
QTL

• ELECTRONIC INSTRUMENTS

Quan-Tech

LABORATORIES INC.

BOONTON, N. J.



INSTRUCTION MANUAL

MODEL 311/310
TRANSISTOR NOISE ANALYZER

For Serial No. 132

QUAN-TECH LABORATORIES, INC.

60 PARSIPPANY BLVD. BOONTON, N.J.

PHONE: DE 4-8500

TABLE OF CONTENTS

Section		*Page*
1	General	1-1
2	Operation	2-0
3	Theory of Operation	3-0
4	Theory and Applications of Transistor Noise	4-0
5	Circuit Description	5-1
6	Maintenance and Calibration	6-1

LIST OF ILLUSTRATIONS

Figure		*Page*
2-1	Transistor Noise Figure Conversion Chart	2-1
3-1	Correction For Low Value of I_N	3-1
4-1	Equivalent Shot and Thermal Noise Generators	4-1
4-2	Equivalent Noise Generators	4-2
4-3	Thermal Noise Voltage Vs. Resistance and Thermal Noise Current Vs. Resistance	4-2
4-4	Shot Noise Voltage Vs. DC Collector Current	4-2
4-5	Shot Noise Current per Root Cycle Vs. DC Current	4-2
4-6	Noise Distribution	4-3
4-7	Noise Distribution	4-3
4-8	Noise Distribution	4-3
4-9	Modification of Test Jig for Field Effect Transistors	4-4
6-1	Input Voltage Barrier Strip	6-1
6-2	Detailed Block Diagram	6-2
6-3	Typical Filter Half Band Widths	6-4
6-4	Internal View from Right Side	6-7
6-5	Internal View from Below	6-8
6-6	Internal View from Above	6-9
6-7	Printed Circuit Board Connector Lug Identification	6-10

ALL SCHEMATICS ARE LOCATED IMMEDIATELY FOLLOWING THE LAST PAGE OF TEXT.

SECTION 1
GENERAL

The Quan-Tech Model 310 Transistor Noise Analyzer was developed specifically to measure the noise inherent in various transistors. This noise is measured simultaneously at three separate frequencies (100 cycles, 1000 cycles and 10 KC). The low frequency bandpasses are necessary for the measurement of 1/f, or fluctuation noise, whereas the higher frequency bandpass is a measure of "shot" noise, thus providing a three point spectrum analysis of the transistor noise characteristic. To facilitate optimum measurements the system will automatically correct for variations in transistor gain when measuring noise.

The Model 310 can make measurements of the input noise voltage as well as the effective input noise current of a transistor, allowing prediction of noise voltages (or noise figure) for any input impedance. Resistances of 500 and 1000 ohms are provided for making noise figure measurements. In addition to noise, Icbo, Iebo and Beta measurements are easily accomplished with the instrument.

SPECIFICATIONS

NOISE RANGE .....0.01 to 3 microvolts per root cycle, full scale, and 1 to 300 pica-amperes per root cycle, full scale.

COLLECTOR VOLTAGE .....0.25 to 30 volts.

COLLECTOR CURRENT .....0.3 to 30 milliamperes, full scale.

LEAKAGE CURRENT ..... Icbo and Iebo - 0.3 to 30 microamperes, full scale.

BANDPASS .....100 CPS, 1000 CPS and 10 KC (Center Frequencies).

BETA RANGE .....10 to 300.

DIMENSIONS .....11" High, 15" Wide, 11" Deep, overall.

POWER INPUT .....117/234 Volts, 60 cycles, 30 watts.

SECTION 2

OPERATION

1. For initial operation of the Transistor Noise Analyzer plug the power cord into a suitable source of power. Refer to the plate on the rear of the instrument near the power cord for the voltage and frequency for which this instrument is wired. See Section 6 for instructions on how to change the input voltage. Turn the power switch on. Since there are vacuum tubes contained in the instrument, a few minutes warm-up will be required.

2. Set panel controls as follows:

   a. NPN/PNP selector for proper type.
   b. Function Switch in "β" position.
   c. Set VOLTS switch and V.ADJ. control for desired transistor collector voltage.
   d. Current switch (MA), to desired current range and I.ADJ. approximately mid-range.
   e. Noise channel attenuators to "3" position.
   f. Base selector switch to E_N position.

3. Insert transistor to be tested and close shield cover which actuates the interlock switch.

4. Instrument should now be operating and "β" meter should indicate operating Beta.

5. Set I.ADJ. for desired operating current.

6. Turn Function Switch to NOISE position and turn noise channel attenuators until noise meter indication is obtained. This is the shorted input or voltage noise "E_N" per $\sqrt{\sim}$ at the filter frequency.

7. To measure the "Noise Figure" of the transistor, set the base selector switch to 1K, measure noise in microvolts and read DB noise figure from the conversion chart (Fig. 2-1). Noise figure for other base resistances may be measured by setting base selector switch to 500 ohms, 10 K ohms (I_N) position or EXT position with a suitable resistor attached to the two insulated terminals adjacent to the test transistor socket.

8. Current noise (I_N) may be measured directly with the base selector switch set to I_N position, the noise meter reading multiplied by 10^{-10} is the noise current in amperes / $\sqrt{\sim}$ at the filter frequency.

9. Leakage currents are measured by setting the function switch to I_{cbo} or I_{ebo} position. The center concentric knob (red dot) indicates the proper microampere full-scale meter range.

NOTE: It may be desirable to reduce the collector voltage when making I_{ebo} measurements.

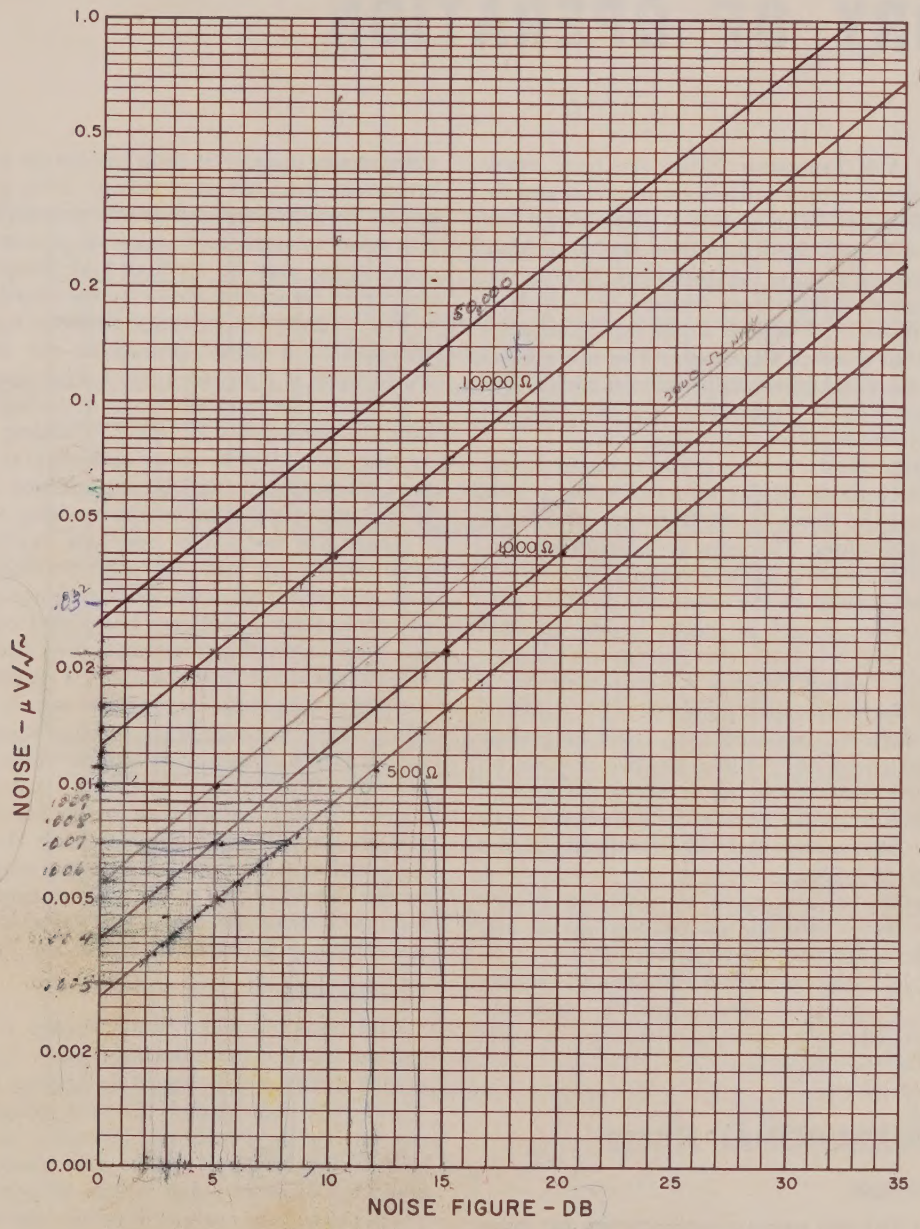


FIGURE 2-1. TRANSISTOR NOISE FIGURE CONVERSION CHART

SECTION 3

THEORY OF OPERATION

The Model 310 Transistor Noise Analyzer offers three frequencies at which noise measurements can be made simultaneously. The standard frequencies are 100 cycles, 1 KC and 10 KC. There are two basic methods of making a noise measurement. One is the commonly known substitution method in which a noise source is inserted at the input and compared with the internal noise of the device. The other basic method is to have a known amplification factor and a known effective noise bandwidth. It is the latter of the two that is employed in the Model 310.

The bandpass filters are carefully measured and calibrated and the gain of the unit is held at a constant value from the input of the transistor under test to the meter indicators. This gain is controlled by inserting a 4 KC calibrating signal at the base of the test transistor. The output of the transistor is then coupled into Amplifier No. 1 as shown in the detailed block diagram, Fig. 6-1. From there is follows through Compressor No. 1, Amplifier No. 2, Compressor No. 2 and Amplifier No. 3, at which point the 4 KC calibrating signal is removed and fed into the Compressor Amplifier, and compared with a Zener reference to control the two compressors. As a result, the gain at this point is held constant. The noise signals are then fed into filter attenuators and the remainder of the filter amplifier circuitry.

Beta measurements are made by inserting a high impedance in series with the calibrating source and the level of the compressor drive is measured.

Control of the collector-emitter voltage and the collector-current is made by two adjustable regulated power supplies. The measurement of leakage currents are made in the standard fashion.

OPERATIONAL HINTS

INSTRUMENTATION

The Model 310 will operate satisfactorily for transistors having a Beta between 10 and 500. Often transistors show a large increase in Beta with increasing collector voltage. If this Beta is in excess of 500 the compressor circuitry fails and erratic behavior is noticeable by large meter fluctuations on the front panel. If Betas of very low values, which often occur at currents below 100 microamperes, are experienced, the compressors operate at their maximum gain and again erroneous readings may result. This may be determined by a further decrease in current and noting if the noise measurement increases proportionately. Another error may be seen at high frequencies if low frequency transistors are being measured. This usually is due to either capacitance between the base-emitter junction or a large decrease in the Beta over and above what it is at the 4 KC calibrating frequency.

It should be pointed out that during Beta calibration the impedance of the calibrating source is approximately 150,000 ohms and that an error in the Beta measurement will be experienced for transistors having input impedances approaching this value.

There are five input positions available: The E_N position, the 500 and 1000 ohm positions, the I_N position and an external source impedance position. If an external source impedance is inserted be sure that the DC drop across this impedance does not exceed 1 volt due to base drive. If this voltage is exceeded the collector power supply may lose regulation. It is often convenient when working with relatively low currents to use an external resistor of 100,000 ohms for measuring the current noise. In this case a correction factor of 10 to 1 should be applied to the meter readings. In making current measurements with the 10,000 ohm, I_N, position, a limit of 1.3×10^{-12} amperes is caused by the thermal noise in the 10 K resistor. If transistors indicate a noise level near this value, a correction for the resistor noise must be made. See Figure 3-1.

TRANSISTORS

The basic transistor noise theory is explained in Section No. 4. However, there are a few applications of this theory which would be helpful to the user.

The shot and thermal noise are straightforward and can be readily calculated. However, the excess noise and avalanche noise effects vary radically with the type of transistors being tested. Defects in transistors which cause large current densities may be easily measured and will show up as excess noise for the given type of transistor. For instance, a fractured or partially fractured base junction will show a large noise voltage E_N. Contamination of the surface or an avalanche condition will show a large value of I_N. Both of these noise generators will usually have 1/f noise far in excess of the normal amount.

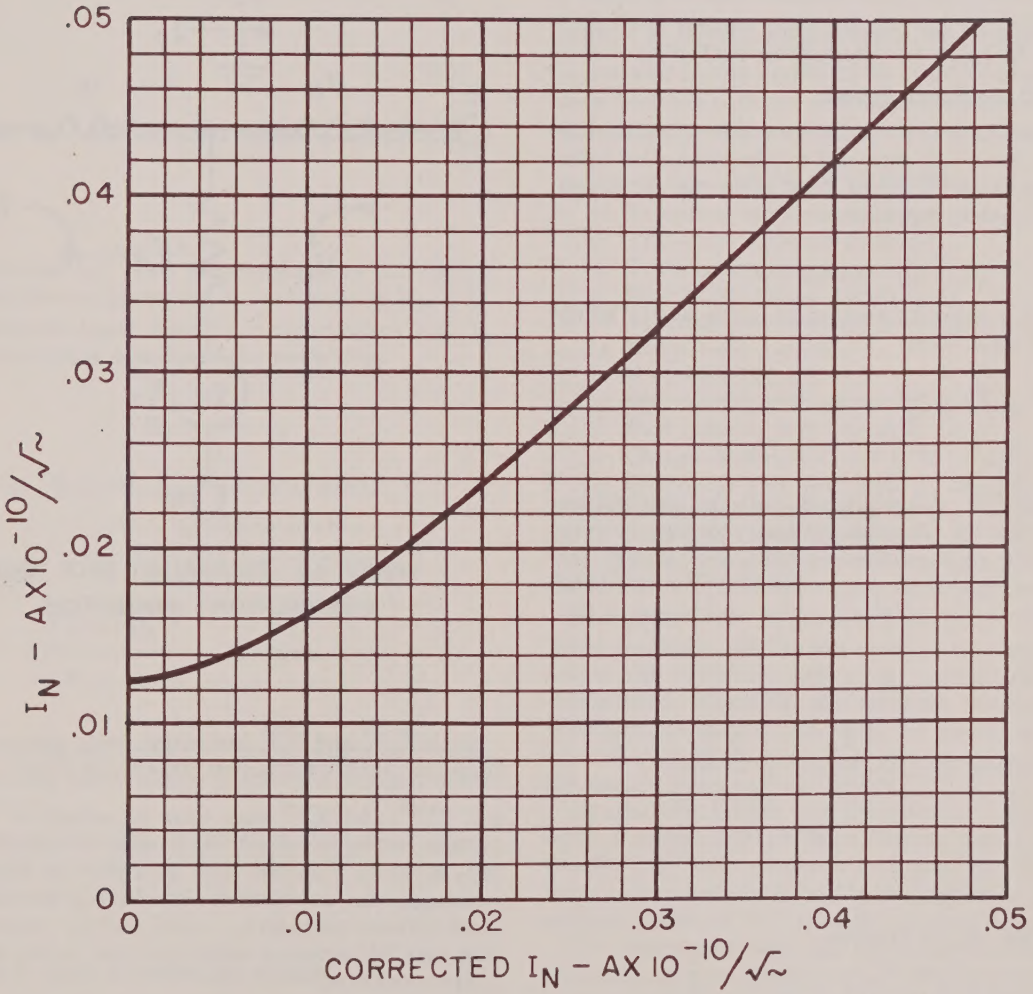


FIGURE 3-1. CORRECTION FOR LOW VALUE OF I_N

SECTION 4

THEORY AND APPLICATIONS OF TRANSISTOR NOISE

An analysis of the internal noise sources of a transistor may be made by referring to Figure 4-1.

SHOT AND THERMAL NOISE

The currents shown are independent of each other and each shows full shot noise. Therefore, the noise currents generated through these paths may be found from the Schottky equation.

$$\overline{I_s^2}^{\frac{1}{2}} = (2 \epsilon I_{DC} \Delta F)^{\frac{1}{2}}$$

Consider a collector current of 1 ma and a bandwidth of 1 cycle, then:

$$\overline{I_{sc}^2}^{\frac{1}{2}} = (2 \times 1.59 \times 10^{-19} \times 10^{-3} \times 1)^{\frac{1}{2}}$$
$$= 1.79 \times 10^{-11} \text{ amps} / \sqrt{\sim}$$

Although $\overline{I_{sc}^2}^{\frac{1}{2}}$ passes through both the base-emitter and base-collector junctions it shows complete correlation and may be considered as effectively through the base-emitter impedance (R_e) only. The resultant noise voltage due to the collector current shot noise in this case is:

$$\overline{E_{sc}^2}^{\frac{1}{2}} = \overline{I_{sc}}^{\frac{1}{2}} R_e$$

$$\text{Where } R_e = \frac{k T}{\epsilon I_e} = \frac{k T}{\epsilon (I_c + I_b)}$$
$$\cong \frac{25 \times 10^{-3}}{I_c}$$

and for 1 ma. $R_e \cong 25$ ohms.

$$\text{Thus } \overline{E_{sc}^2}^{\frac{1}{2}} = 1.79 \times 10^{-11} \times 25 =$$
$$0.44 \times 10^{-9} \text{ volts} / \sqrt{\sim}$$

$r_{b'b}$, the base spreading resistance contributes thermal noise and may be calculated from Nyquist's equation

$$\overline{E_t^2}^{\frac{1}{2}} = (4 k T R \Delta F)^{\frac{1}{2}}$$

and for a 100 ohm $r_{b'b}$

$$\overline{E_t^2}^{\frac{1}{2}} = 1.26 \times 10^{-9} \text{ volts} / \sqrt{\sim}$$

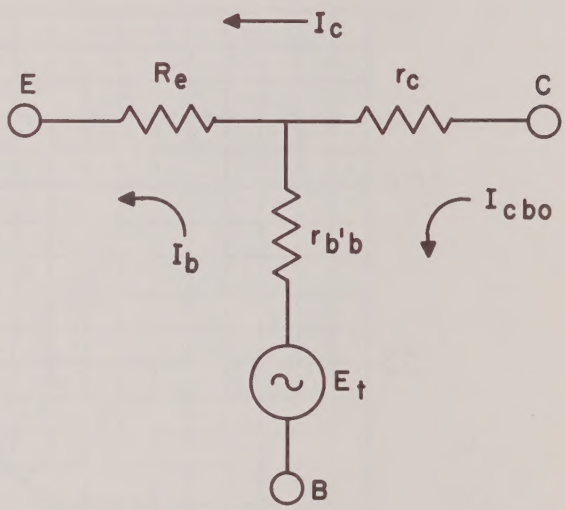


FIGURE 4-1. EQUIVALENT SHOT AND THERMAL NOISE GENERATORS

Both $\overline{E_{sc}^2}^{\frac{1}{2}}$ and $\overline{E_t^2}^{\frac{1}{2}}$ are major noise sources in the transistor even with a zero impedance source generator. $\overline{E_{sc}^2}^{\frac{1}{2}}$ and $\overline{E_t^2}^{\frac{1}{2}}$ may thus be added in an rms fashion and be considered as a noise voltage generator (E_N) in series with the base as shown in Figure 4-2. Although the d-c currents I_b and I_{cbo} develop shot noise currents through $r_{b'} + R_e$ and $r_{b'}$ respectively, they may be neglected unless very low values of β and I_c are considered.

When large input impedances are considered the noise currents resulting from I_{cbo} and I_b are the major contributors. Thus $\overline{I_{sb}^2}^{\frac{1}{2}} = (2 \epsilon (I_b + I_{cbo}) \Delta F)^{\frac{1}{2}}$.

If $I_{cbo} = 1 \times 10^{-6}$ amperes and assuming a β of 100 with an I_c of 1×10^{-3} amperes.

$$\text{Then } \overline{I_{sb}^2}^{\frac{1}{2}} =$$
$$[2 \times 1.59 \times 10^{-19} (10 \times 10^{-6} + 1 \times 10^{-6}) 1]^{\frac{1}{2}}$$
$$= 1.87 \times 10^{-12} \text{a} / \sqrt{\sim}$$

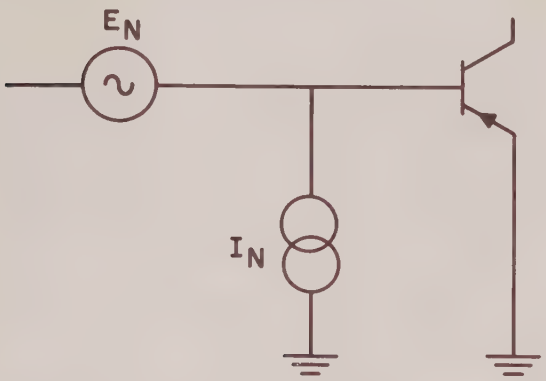


FIGURE 4-2. EQUIVALENT NOISE GENERATORS

The current $\overline{I_{sb}^2}^{1/2}$ may be considered as the equivalent noise current generator, I_N, as shown in Fig. 4-2.

An optimum input impedance occurs when both I_N and E_N contribute equally to the noise thus:

$$R_o = \frac{E_N}{I_N}$$

and for the idealized transistor considered,

$$R_o = \frac{(.44^2 + 1.26^2)^{1/2} \times 10^{-9}}{1.87 \times 10^{-12}} = \frac{1.34 \times 10^{-9}}{1.87 \times 10^{-12}} = 720 \text{ ohms.}$$

There are second order corrections which have been omitted in the above theory of shot and thermal noise in transistors.

For a more thorough treatment of the subject, reference should be made to "Fluctuation Phenomena in Semi-conductors" by A. van der Ziel.

EXCESS (1/f) AND AVALANCHE NOISE

In addition to the shot and thermal noise sources there are excess noise and avalanche noise mechanisms. The exact cause of the excess noise is not clearly understood. However, it can be expressed by the following equation:

$$\overline{I_{ex}^2}^{1/2} = (C\, I^a\, F^\gamma)^{1/2}$$

The exponent a is very close to 2 and the value of γ is about -1.09. Little error is involved if the excess noise current is assumed to be proportional to the d.c. current and to have a 1/f power spectrum. The constant C is determined experimentally since it is a function of material and shape factor.

It is difficult to predict the magnitude of the excess noise in a transistor. I_c, I_b and I_{ebo} all contribute. However, their relative magnitudes are dependent upon the type of transistor structure and its operating conditions.

The above noise mechanisms (thermal, shot, and excess) all have a Gaussian amplitude distribution which is well defined mathematically. Avalanche noise on the other hand may have amplitude and frequency distributions that are difficult to define. Noise of this type is generated by the avalanche or multiplication phenomena between collector and base, and often increases exponentially with increasing collector voltage.

TABLE OF SYMBOLS

- B = Transistor base terminal
- C = Transistor collector terminal
- E = Transistor emitter terminal
- E_{sc} = Shot noise voltage due to I_c
- E_t = Thermal noise voltage due to $r_{b'}$
- I_{ex} = Excess noise current
- I_s = Shot noise current
- I_{sb} = Shot noise current due to I_b and I_{ebo}
- I_{sc} = Shot noise current due to I_c
- ϵ = Charge on electron, 1.59×10^{-19} coloumbs.
- k = Boltzman's constant. 1.38×10^{-23} joules / °C
- T = Temperature in degrees Kelvin
- R_o = Optimum source resistance

ANALYSIS TECHNIQUES

The Quan-Tech Models 310 and 311[1] Transistor Noise Analyzers, far beyond mere total noise measurements, can provide a substantial amount of detailed information regarding the internal condition of a transistor, indicating not only the region in the device where a fault exists, but also in many instances the specific nature of the defect.

In addition, proper interpretation of the results of noise measurement provides a truly sound basis for establishing "approved vendor" lists and incoming-inspection standards from the standpoint of the most realistic yardstick for "quality" currently available.

To understand best the noise characteristic of a transistor, it is advisable to begin by determining the level of noise that would be generated were the transistor an "ideal" one (i.e., one generating thermal and shot noise only, with no 1/f or avalanche[2] noise present).

[1]The Models 310 and 311 are essentially similar, except that the Model 311 is intended primarily for operation at low values of collector current. It should be noted that as long as the test transistor is operated within the collector-current range of the instrument, system sensitivity is adequate to measure down to theoretical minimum noise values. The sensitivity of these instruments cannot be tested without a transistor in the test jig. See Section 6 for detailed information on making system sensitivity test.

[2]See, "Electrical Noise and Component Reliability," published by Quan-Tech Laboratories, Inc., for a general discussion of various types of electrical noise.

Noise current and noise voltage in this "ideal" transistor may be readily found from the following expressions and the accompanying graphs:

Ideal Noise Voltage $E_n = (E^2 \text{ thermal} + E^2 \text{ shot})^{\frac{1}{2}}$

Ideal Noise Current $I_n = (2q\,[I_b + I_{cbo}])^{\frac{1}{2}}$

Thermal and shot noise voltages originate respectively from the base spreading resistance and from the base-emitter junction (due to emitter current). They may be determined for the given operating conditions from the graphs in Figure 4-3 and Figure 4-4 respectively. Shot noise current may be determined from Figure 4-5.

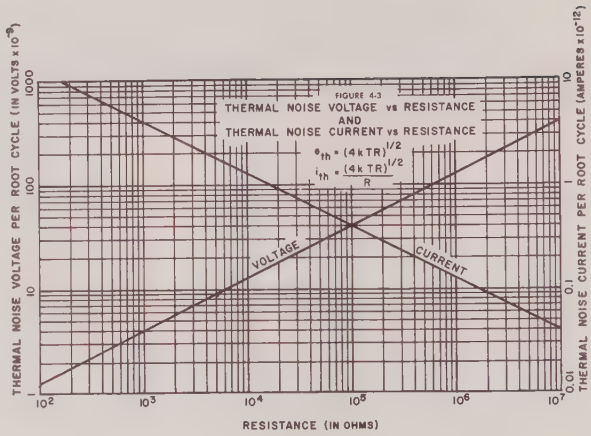
These "ideal" noise current and voltage values represent the theoretical minimum of noise the device could exhibit for the given operating condition. However, no transistor will operate at this minimum value. Depending on the individual transistor, 1/f noise will be present, and it is possible that avalanche noise, too, may contribute to the total noise. Measurement with the Quan-Tech Model 310 or 311 will reveal the extent to which the device deviates from the "ideal."

1/f noise, dependent upon current density within the device, is of inestimable value in revealing defects in the transistor.

a) *Base-emitter region* — Such faults as defective contacts, fractures or irregularities in the junction may be readily detected by measuring noise voltage (E_n) with the transistor operated under high-current conditions. (NOTE: Care should be taken to see that the total dissipation rating of the transistor is not exceeded during this test. Frequently, it is necessary to reduce the applied voltage before increasing the current to protect the transistor from damage.) These conditions are indicated by an abnormally high level of 1/f noise. It should be noted that what constitutes a "normal" level of 1/f noise varies from transistor type to transistor type. It is to be expected, for example, that devices of small cross section, such as mesa transistors, generally have a substantially higher 1/f noise level than do larger types. The norm for a given type under a given operation condition may be readily determined by making and comparing measurements of a number of units.

b) *Base region* — Defects in the base region similar to those in the base-emitter region may be detected by measuring the 1/f noise current (I_n) at lower value of applied current than for the base-emitter test.

c) *Collector-base region* — Surface contamination may be detected by testing for 1/f noise current (I_n) at very low collector current (a few hundred microamperes) and gradually increasing the collector voltage. If the noise current increases approximately proportionately with voltage, surface contamination is most probably present, and is acting as a semiconductor-resistor across the collector-base junction. If



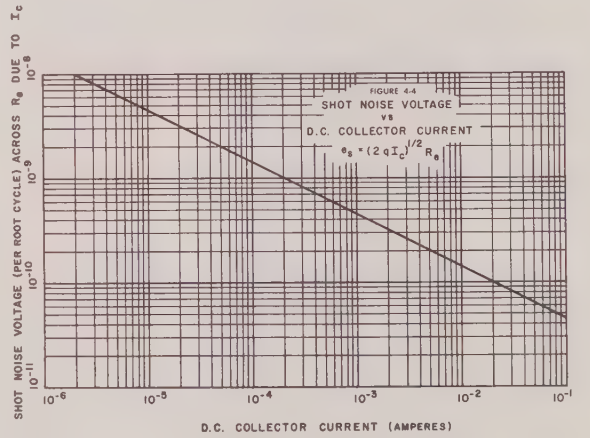
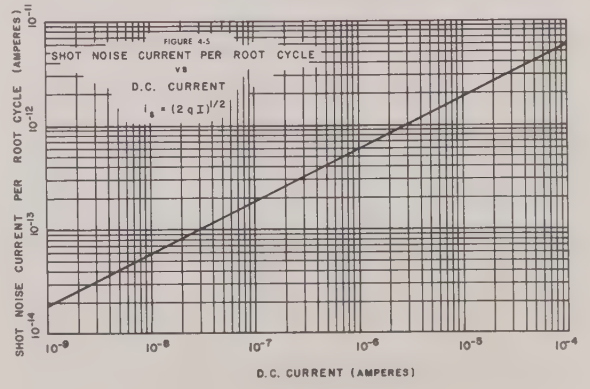


FIGURE 4-4
SHOT NOISE VOLTAGE
vs
D.C. COLLECTOR CURRENT
$e_s = (2qI_c)^{1/2} R_e$
SHOT NOISE VOLTAGE (PER ROOT CYCLE) ACROSS R_e DUE TO I_c
D.C. COLLECTOR CURRENT (AMPERES)



the noise increases abruptly, or essentially exponentially with the voltage, the collector-base junction is breaking into avalanche. It should be noted that *any* transistor will avalanche eventually as the voltage is increased. It is when the avalanche takes place *within rated operating voltages* that trouble is indicated, probably in the form of an irregularity of the collector-base junction.

d) *"Sleepers"* — This term has been applied to a particular type of transistor defect that is characterized by the fact that on immediate examination no excessive noise problem is evident. However, as the test is prolonged up to a period of many hours, the noise level rises. Generally, if the test current or voltage is interrupted, the transistor returns to its state of quiet operation. However, as the test progresses once more, the transistor will again increase in noise output. To detect the "sleeper", tests of as long as 24 hours or more may be required. Fortunately, in the practical case, "sleepers" are quite rare, and once a reliable vendor is found, this problem may generally be negelected.

Vendor Selection

Even limited experience with transistor noise analysis will reveal that the differences in noise characteristic between transistors of the same type from different manufacturers varies very broadly. A significant evaluation of quality of a given transistor type may be made by testing a batch for noise, and plotting the results in the form of distribution graphs as shown in Figures 4-6, 4-7 and 4-8. All three of these graphs were drawn for the same type of transistor — a medium frequency germanium device. Figure 4-8 shows an excessively broad spread, indicating a serious lack of production control on the part of the manufacturer. Such a spread would eliminate this supplier from the "approved vendor" list. Figure 4-7 shows a substantially better spread, but still the grouping is more than one might desire. Figure 4-6 shows an excellent pattern, with all units closely grouped around a low noise level. This graph shows excellent process control and justifies placing the manufacturer on an "approved vendor" list for transistors of this type.

It should be noted that vendor selection of this type will not obviate the necessity for checking transistors at incoming inspection for noise, but it will go a long way toward reducing the number of rejects at this inspection point, and thus substantially reduce the real cost of the transistor to the user.

Production Testing

The extent to which individual transistors should be inspected for noise depends upon the degree of re-

FIGURE 4-6

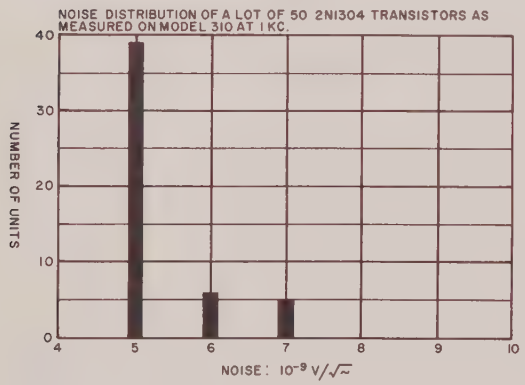


FIGURE 4-7

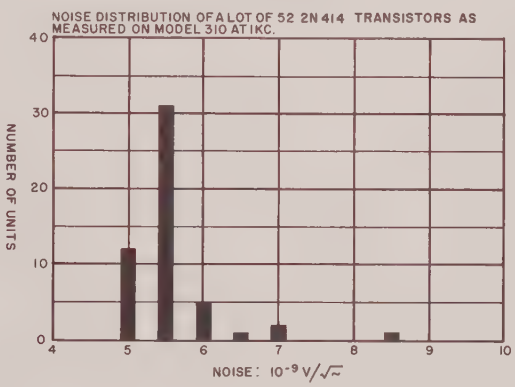
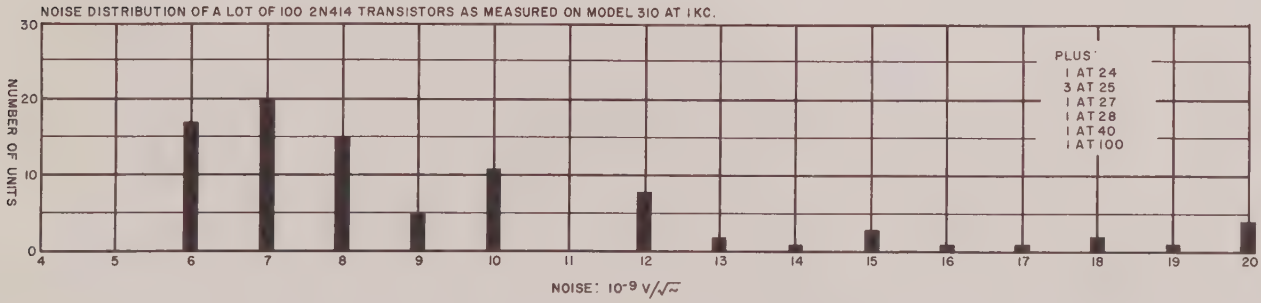


FIGURE 4-8



liability required of the equipment in which they are to be used.

In many circumstances where *extreme* reliability is not required, a single noise measurement per transistor usually suffices. The common practice is to measure noise voltage with the transistor operated under conditions of the highest voltage possible within the ratings of the transistor, and at a collector current value comparable to that of the actual circuit. With the resistance selector at 1000 ohms, noise figure measurements may be readily made.

For maximum reliability, it is advisable to measure both noise current (I_n) and noise voltage (E_n) under conditions of low collector current and high voltage as well as high collector current and low voltage. In this way, a detailed analysis of each transistor may be made.

Field-Effect Transistors

The Models 310 and 311 may be used for either laboratory or production testing of field-effect transistors by following the steps outlined below:

1. Set base resistance switch to EXT position.
2. Turn current control fully CCW.
3. Ground emitter terminal (E) in test jig to shield strap.
4. Remove shorting bar between terminals.
5. Rewire terminals in test jig as shown in Figure 4-9.

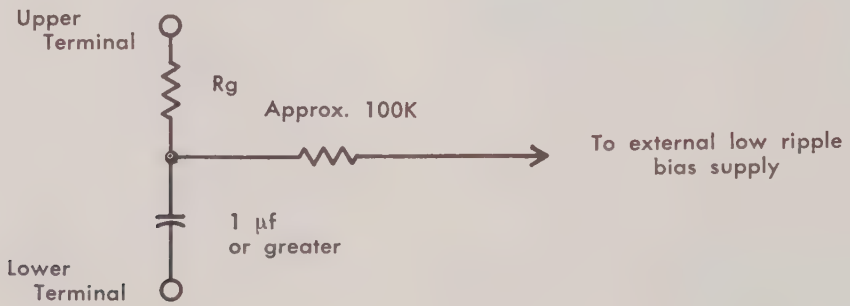
The Models 310 and 311 will measure noise in any field-effect transistor within the limits outlined in Section 3. The AGC circuit of the instruments will function over the following ranges of G_m:

	G_m Range
Model 310 —	1000 μmhos to 100,000 μmhos
Model 311 —	100 μmhos to 40,000 μmhos

Additional Applications Information

The fullest capabilities of the Models 310 and 311 may well not be appreciated by the user who is not familiar with the equipment. Every effort has been made by Quan-Tech Laboratories to make both the Instruction Manual and associated applications notes as complete as possible, but since it is impossible to anticipate all of the questions that might arise, Quan-Tech's Engineering Department will provide detailed, individual advice and instructions on the capabilities and functions of the equipment.

If you should have any additional questions concerning the use or operation of the Models 310 or 311, address your inquiry to the Engineering Department, giving as many particulars as possible. Information may also be obtained by telephone, and all inquiries will receive prompt and complete attention.



NOTE: Exact circuit values are not critical, but should be of the general magnitude shown.

FIGURE 4-9 MODIFICATION OF TEST JIG FOR FIELD EFFECT TRANSISTORS

SECTION 5

CIRCUIT DESCRIPTION

POWER SUPPLIES

Power is supplied to the instrument via line plug P101, fuse F101, front panel power switch S101 and the primary of the main power transformer T101.

26 V General Supply

The 26V General Supply furnishes power for the vacuum tube voltmeter heaters and all the noise measuring circuits with the exception of the transistor under test. Conventional regulated power supply design is used; its operation is briefly as follows:

Unregulated DC is supplied by secondary #1 of T101, bridge rectifier CR301, 302, 303, 304 and capacitor C301. A ½-amp. fuse F301 is incorporated to prevent damage to the pass transistor Q304 in case of accidental short circuit or overload. Control for the pass transistor is obtained from the voltage reference Zener diode CR305, balanced differential transistor pair Q301, Q302 and amplifier Q303.

15 V Emitter Supply

The 15V Emitter Supply is used solely to control the current in the transistor under test by means of the front panel I ADJ., potentiometer R516 and current limiting resistors R528 through R532 as selected by the MA range selector switch.

The operation of this supply is the same as the 26V general supply and need not be repeated here.

VTVM Supply

The VTVM Supply is used to supply a positive 105V and a negative 105V source for the two vacuum tube voltmeters. V502 is used to measure the collector current of the test transistor and V501 is used to measure the emitter-collector voltage of the test transistor, and also to control the regulated collector power supply. Its operation is as follows:

AC voltage from secondary #5 is rectified in the voltage doubling circuit consisting of CR101, CR102 and capacitors C102 and C103. This voltage is filtered by the R C filter consisting of R101, C104, and R102 and VR tubes V101, V102. The VR tubes also regulate this voltage and provide a midtap supplying both a positive and negative 105V. This midtap is connected to a point on the test transistor collector supply buss. The minus 105 is also separately filtered by R103, C105 and supplies minus 105V for the collector supply vacuum tube voltmeter.

Current Meter Circuit

The current meter is basically a high impedance, 1 volt, vacuum tube voltmeter and measures current by measuring the voltage drop across a resistor in series with the test transistor. This resistor value is selected by means of S503 for the different collector current and leakage current ranges.

Vacuum tube V502 is a twin triode arranged in a balanced differential cathode follower circuit driving a meter (M502) and calibrating resistor (R538) connected between the two cathodes. This circuit is calibrated to read full scale when 1 volt is applied between the two tube grids. Switch S501L and S501M serve to maintain proper polarity when the NPN/PNP switch is changed.

Voltmeter Circuit

The voltmeter is also a high input impedance vacuum tube voltmeter circuit which also serves as a servo control loop to maintain a pre-set voltage between the emitter and collector of the test transistor. Its operation is as follows:

Vacuum tube V501 is a twin triode arranged in a balanced differential cathode follower circuit driving a meter (M501) and resistor connected between the two cathodes. The meter resistors are switched for each voltage range and calibrated to give correct meter indication for each voltage range, 1 volt through 30 volts, when this voltage is applied between the two grids. S501E and S501F serve to maintain proper polarity when the NPN/PNP switch is changed. The cathode resistor of the right half section of V501 (see schematic C3105) consists of V ADJ. resistor R512 and fixed resistor R513. The moveable arm of R512 permits the servo control line to be offset by the desired collector voltage and thus control the collector supply at any level desired between 0 and 30 volts.

Collector Supply

The Collector Supply is a variable regulated power supply adjustable from 0 to 30V capable of supplying 30 milliamperes. It is used to supply collector voltage to the transistor under test. Theory of operation is as follows:

AC voltage is supplied by secondary winding #3 of T101. This voltage is rectified by a bridge rectifier CR203, CR204, CR205 and CR206. C203 is the filter and storage capacitor. This unregulated voltage is applied to the collector of pass transistor Q205. The base

of Q205 is controlled by the differential balanced transistor pair Q201, Q202 and emitter follower Q203. CR208 and CR209 are clamping diodes and prevent excessive voltages or currents from damaging the transistors. These diodes are normally non-conducting. Voltages for the control and differential pair transistors are supplied by secondary winding #4 of T101, half wave rectifiers CR201, CR202 and capacitors C201 and C202. CR207 is a Zener diode and regulates the collector voltage of Q201 and Q202. Q204 is used to limit the maximum current which can be drawn from the power supply and operates as follows. The base of Q204 is normally held approximately 0.75V positive with respect to its emitter by the current through R210 and the voltage drop across the forward biased diode CR212 which is connected to the emitter of the pass transistor Q205. This bias prevents Q204 from conducting and permits normal operation of the collector supply. When currents in excess of approximately 35 milliamperes is drawn from the emitter of Q205 the voltage developed across R211 and R212 exceeds this 0.75V and transistor Q204 begins to conduct and clamps the base of Q203 to the negative regulated buss cutting off the drive to pass transistor Q205 and thus limiting the maximum current to a safe value. CR210, CR211 and the emitter base potential voltage drops serve to supply collector voltage for the current limiting transistor Q204. CR213 is a back biased diode to prevent damage and lockout of the control if reverse voltages are applied to the supply. Operation of the servo line and collector voltage level is as follows: Assume operation is for NPN configuration. The negative side of the collector supply is grounded via NPN/PNP switch S501A. The positive side is connected to the test transistor collector via S501B, current range selector switch S503A, function switch S505A, transformer T501, interlock switch S504 and S505C. The collector voltage is sampled and applied to the voltmeter grid (right hand section Sec. C-3105) via isolating resistor R533 and switch S501E. The voltage at the emitter is sampled and applied to the other voltmeter grid causing an unbalanced condition of the two cathode followers by the amount of this voltage (see voltmeter operation). As the collector supply voltage is dependent on the voltage difference between the bases of the differential balanced transistor pair Q201, Q202 and as these bases are connected across the cathode V501 and cathode resistor V. ADJ. (R512) the output voltage will shift in a direction to maintain a balanced condition in these transistors. The collector voltage will approximately be equal to the voltage drop between the cathode of V501 (right section) and the arm of V. ADJ. (R512). Operation in the PNP transistor position is similar but supply and test transistor voltages are reversed in polarity.

4 KC Oscillator

The 4 KC Oscillator is used to supply an accurate reference signal at the base of the transistor under test and also to operate the automatic gain control system which allows accurate noise measurements independent of the Beta of the transistor under test. Operation is as follows: Negative voltage is supplied from the 26 volt general supply through R601 and voltage regulating Zener diode CR601. The oscillator is of the LC type using the primary of a stable torroid transformer and capacitors C601, C602 and C603 as the frequency determinates. This frequency is tuned to 4.00 KC. The transistor Q601 operates in a grounded base configuration and obtains its emitter excitation from a capacitance divider network approximately 30:1 consisting of C601 and C602. This provides a low impedance drive for the emitter of Q601. The collector output drives from a tap on the transformer T601 also a relatively low impedance point and R604 to further minimize any collector loading on the LC tank circuit. This results in an extremely stable oscillator whose level is controlled by the stable Zener voltage of CR601 and is independent of transistor characteristics or supply voltage. Output voltage at 4.00 KC is obtained from a very low impedance winding and adjustable by means of R607 to a value of 5.1 millivolts at the Beta calibration jack J501.

Base Selector Switch

The base selector switch located on the test transistor panel provides a selection of impedance for the base of the transistor under test. In the E_N position the base is returned to ground via R544 a 1 ohm resistor. This resistor is part of a divider network R544 and R546 supplying the low level carrier signal necessary to operate the AGC system and serves as the noise level reference generator. The 500 and 1K positions permit measuring the "Noise Figure" of the transistor test and the I_N position permits direct measurement of the input current noise. S505F when in the "β" position permits driving the test transistor base at a higher level (5.1 millivolts)via the high Q tank circuit L501, C509 and C510 acting as a constant current source at 4 KC to permit direct Beta measurements.

T 501

Transformer T501 is a special band pass current transformer designed to permit transfer of the noise current and 4 KC carrier signal from the transistor under test to amplifier #1. The transformer has a bandpass from 100 cycles to 100 kilocycles.

Amplifier #1

Amplifier #1 is a three stage extremely low noise transistor amplifier utilizing NPN, PNP, NPN configuration. Q701 operates as a grounded base amplifier, the emitter impedance properly terminating the secondary winding of T501. Q702 and Q703 operate as grounded emitter amplifiers with maximum overall negative feedback, assuring stable gain and low output impedance to drive the following compressor.

Compressor #1 and #2

The compressors #1 and #2 operate in an identical manner and will be discussed together. The compressor serves as a variable attenuator consisting of resistor R802 and a pair of transistors Q801, 802 connected as diodes operating in parallel to alternating current which act as the lower leg of a voltage divider network. As the AC impedance of a diode is inversely proportional to the DC current, the impedance of this lower leg of the network is approximately $= \frac{13 \text{ ohms}}{I_{dc} \text{ in milliamperes}}$ and is linear over a current range of several hundred to one. Compressor #2 comprising Q807, Q808 and R816 act in a similar manner, the amount of signal compression being controlled by AGC amplifier and reference network.

Amplifier #2

Amplifier #2 is typical of several amplifiers used in this instrument, conventional transistor circuitry is employed, Q803 is the input PNP transistor grounded emitter configuration. Q804 is NPN driver for the complementary symmetry push pull output pair Q805 and Q806. Overall negative feedback serves to stabilize the overall gain, reduce crossover distortion and provide a low impedance circuit. Voltage gain is approximately 80 and incorporates a temperature compensating resistor R808 to compensate for the temperature characteristics of the diode compressors.

Amplifier #3

Amplifier #3 is identical to Amplifier #2 and is used to drive the 4.00 KC notch filter of the AGC system and the variable attenuators of the noise filter systems.

4 KC Notch Filter

The 4 KC Notch or AGC filter is a series resonant LC filter of high "Q", consisting of C905, C907 and L901. This filter serves a dual purpose. It removes the major portion of the 4 KC oscillator carrier signal from the noise filter spectrum and drives the compressor amplifier.

Compressor Amplifier

The compressor amplifier while basically similar to Amplifier #2 and #3 operates in a slightly different manner. As the 4 KC notch filter requires a low terminating impedance to maintain a reasonable tank circuit Q the base of Q1007 is grounded to ac and the emitter feedback point, which has an extremely low impedance, is used as the input. Thus Q1007 operates as a PNP grounded base amplifier to drive Q1006 as an NPN grounded emitter amplifier which in turn drives the complementary symmetry pair Q1004 and Q1005.

Compressor Driver

The function of the Compressor Driver is to convert the 4 KC carrier signal to a DC current to control the signal compressors maintaining the overall noise loop gain to a constant. Operation is as follows: CR1002 and CR1003 rectify the 4 KC carrier signal. C1002, R1006 and C1001 filter the DC and form the proper time constant for the AGC system. The rectified DC signal is applied to the base of Q1003 of the differential transistor pair. The base of Q1002 is clamped to the Zener voltage level of CR1001. This leaves Q1001 in a cut-off condition until the rectified 4 KC carrier level is equal to the Zener voltage. Q1001 then turns on and maintains sufficient current to the compressors to maintain this level. M1001 is a 5 milliampere meter calibrated in terms of Beta and thus measures the current gain of the transistor under test when the function switch is in the "β" position.

Filter Attenuator

The filter attenuators for all noise channels are identical and receive their common signal from the output of Amplifier #3 through resistor R913 which permits notching the 4 KC carrier from the noise spectrum. These attenuators are of the simple ladder type of 3,000 ohms impedance.

1 KC Filter Amplifier

This amplifier serves to increase the noise level, provides a high input impedance to eliminate loading the attenuator and provide a low impedance for the following noise filter. The operation of this amplifier is identical with that of Amplifier #1 and #2 with the exception of the 27 ohm gain determining resistor R1313 which is a stable non-temperature sensitive type as temperature/gain correction is not required at this point.

1 KC Filter

The purpose of the bandpass filter is to sample the noise spectrum at 1 KC and reject all other noise or signals. The filter is a three stage maximumly flat type using stabilized torroidial coils and mylar tuning capacitors, hermetically sealed at the factory. No further adjustments are required.

Meter Amplifier

The meter amplifier (Ass'y #3159) and meter rectifier board (Ass'y #3160) will be discussed together. The amplifier is similar in operation to the previous amplifiers. Q1401, a PNP transistor drives Q1402 a NPN type grounded emitter which in turn drives Q1403 and Q1404 a complementary symmetry pair supplying a low impedance drive for the meter rectifiers CR1401 and CR1402. The noise signals are rectified and measured by M1401 a 500 microamperes meter. The meter-rectifier return is applied to the emitter of Q1401 providing maximum negative feedback and linearity.

CR1403 is a forward conducting diode to protect the meter against overloads. R1415 permits adjustment of the DC analog to 1 volt DC which is available at J1402. R1413 the screw driver adjustment in the rear of the noise channel permits adjustment and calibration of the noise channel. J1401 permits oscilloscope observation of the noise envelope at the filter frequency.

10 KC and 100 KC Noise Channels

The 10 KC and 100 KC noise channels are identical to the 1 KC channel with the exception of the filter frequency and the roll off capacitor on the input of the meter amplifier.

100 Cycle Amplifier and Filter

The 100 Cycle Amplifier is quite different, being a three section synchronously tuned type utilizing a double emitter follower or grounded collector stage at the input and between each filter section to provide power gain, isolation and high stability. The inductors are highly stable toroidal type, hermetically sealed at the factory and adjusted to resonate with C1102, C1103 and C1104. No further adjustment is required.

100 Cycle Meter Amplifier

The 100 cycle meter amplifier and rectifier (Ass'ys 3155 and 3156) operate the same as the 1 KC meter amplifier and meter rectifier and need not be again discussed here.

SECTION 6

MAINTENANCE AND CALIBRATION

The components and transistors in the Model 310 are conservatively rated and should provide long and trouble free service. If, however, the instrument has been damaged and recalibration or alignment is required, the following instructions should be followed explicity, or the instrument returned to the factory. Instructions are given on the Warranty page for the procedure to be followed should it be desired to return the instrument for any reason.

Although the Model 310 is a complex instrument, trouble shooting can readily be done in sections as indicated in the block diagram, Fig 6-1. Standard transistor servicing care should be used throughout.

Do not change any adjustments without a thorough knowledge of the circuit and the functions of the adjustment.

Transistors can be easily damaged with large transient voltages. Therefore, take great care not to short any terminals when making measurements on the printed-circuit boards. In soldering to the boards, have the iron only hot enough to make a rapid clean solder joint. Do not apply any force which would tend to push the copper away from the board.

NOTE: Refer to Figs. 6-4, 6-5 and 6-6 for component locations.

1. *Removal from Case.*

To remove the unit from the case, proceed as follows:

a. Remove the two right-hand rubber feet and the four binder head screws from the bottom of the case.

b. Slide the unit gently out of the front of the case.

2. *Changing Input Voltage.*

This instrument has been designed to operate from a 117 V.A.C. or a 234 V.A.C. power source. The plate on the rear of the instrument near the power cord indicates the voltage and frequency at which the instrument should be operated.

Should it be desired to change the input voltage,

1. Remove the instrument from the case.

2. Change the transformer primary connections by moving the jumpers on the 4 terminal barrier strip located near the power cord (See Fig. 6-1).

3. Change the fuse. For 117 V.A.C. operation, the fuse should be ½ Amp. Slow Blow; for 234 V.A.C. operation the fuse should be ¼ Amp. Slow Blow.

4. Reverse the plate located near the power cord to read the correct voltage.

3. *Power Supplies.*

Apply line power to the unit. The pilot light should light indicating the power transformer is operating.

General Power Supply

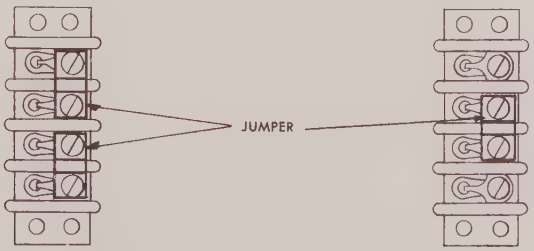
a. Measure voltage at the General Power Supply plug-in board (assembly 1868) between terminal "A" and ground.

b. Adjust R301 for minus 26V DC at this point.

Emitter Supply

a. Measure voltage at the Emitter Power Supply plug-in board (assembly 1869) between terminals "A" and "F".

b. Adjust R401 located on assembly 1869 for 15V DC. Terminal "A" is minus.



For 117 V.A.C. operation **For 234 V.A.C. operation**

FIGURE 6-1. INPUT VOLTAGE BARRIER STRIP

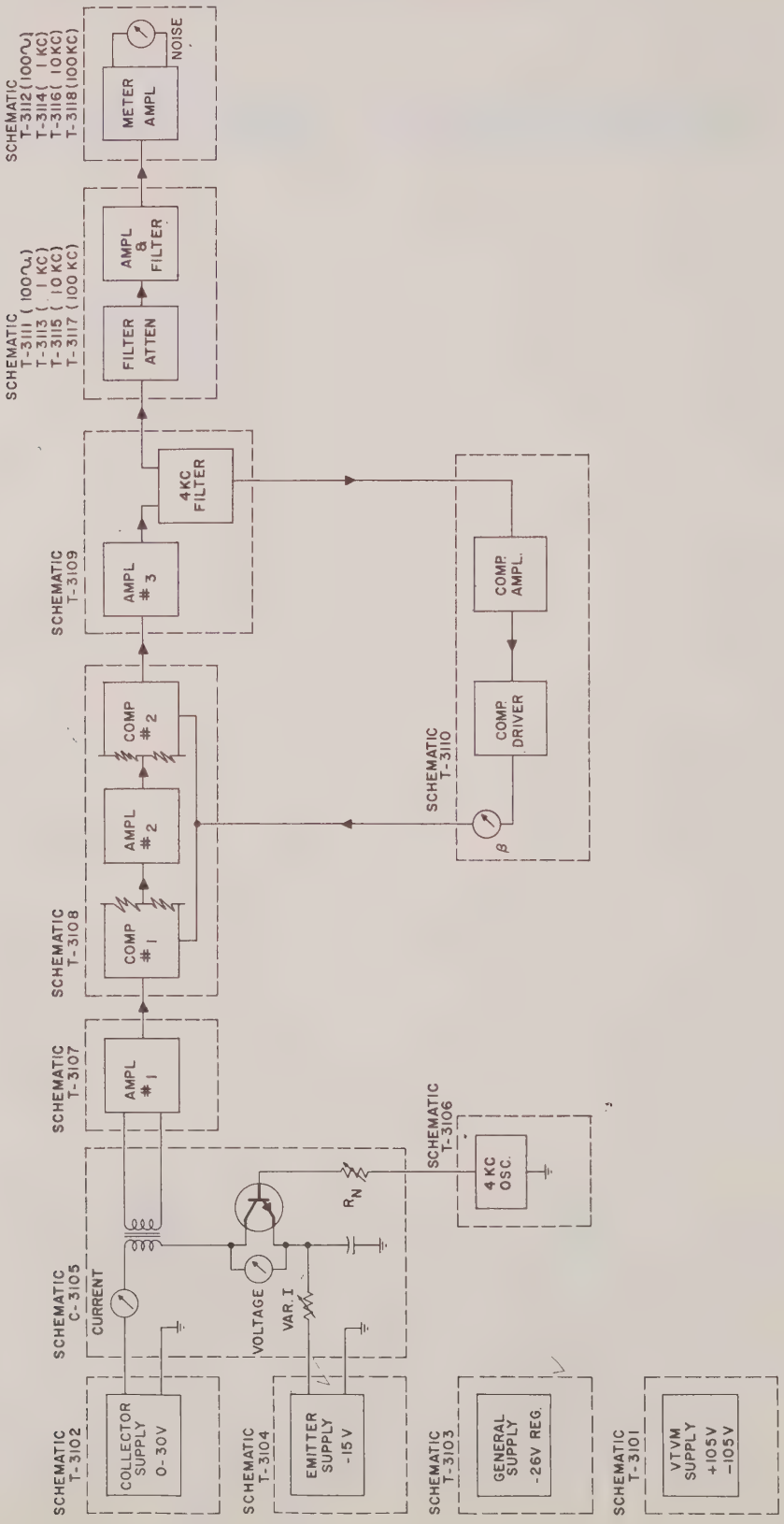


FIGURE 6-2. DETAILED BLOCK DIAGRAM

ERRATA

Model 311 Instruction Manual

On Model 311, Section 6:

1. Delete section titled "Collector Supply".
2. Under "Current Meter Calibration", paragraph a. and b. "10 milliamperes" should read "1 milliampere" and "10 MA" should read "1 MA".
3. Under "D.C. Voltmeter Calibration", paragraph d., "current range switch to 30" should read "current range switch to 1000 uA".
4. Under "Compressor Filter", paragraph d. delete, and paragraph e. "Voltmeter" should read "AGC".
5. Delete sections on "Base Input Tank Circuit Adjustment" and "Beta Meter Calibration".
6. Add "AGC Meter Calibration":
   - * a. Insert low leakage silicon transistor in test jig. Set current to 1.5 uA and voltage to 5V.
   - * b. Adjust R1009 so that AGC meter just starts to bounce.
   - c. Increase current to 1 uA and AGC meter should read on line between red and white. (It may be necessary to pad R1019 - Assy #1865)
7. Under section "Noise Meter Calibration" add after "To calibrate, proceed as follows:
   - a. Set FUNCTION switch to NOISE position.
   - b. Insert a low leakage silicon transistor in the test jig and apply 100 uA and 5 Volts." Paragraph a,b,c, d,e and f should be changed to c,d,e,f,g and h respectively.

* ADJUST R1009 SO AGC METER JUST STARTS TO BOUNCE AT 1μA WHEN I ADJ. IS VARIED R1009 THERE

Collector Supply

a. Insert a transistor capable of handling 40 milliamperes in the front panel test jig socket.
b. Connect a DC milliammeter in series with the collector lead.
c. With shield cover and interlock switch open, set R539 screw driver adjustment control (located just below and to the right of the CURRENT meter) for zero current meter indication.
d. Set front panel controls as follows:
   - FULL SCALE VOLTS switch at 3
   - V. ADJ. for approximately 3 volts
   - CURRENT RANGE switch 30 MA
   - I. ADJ. approximately mid range
   - FUNCTION switch to NOISE
   - BASE SELECTOR switch to E_n position
e. Depress shield cover interlock switch
f. Advance I. ADJ. current control until milliammeter indicates approximately 34 milliamperes.
g. Adjust R212 located on Collector supply plug-in board (assembly 1871) until voltmeter indicates a loss of power supply regulation.

Current Meter Calibration

a. With a milliammeter in series with the test transistor collector and approximately 3V on collector, set I. ADJ. control for 10 milliamperes collector current.
b. Adjust R538 located on assembly 1865 for a current meter indication of 10 milliamperes with the current selector switch in the 10 MA position.

D.C. Voltmeter Calibration

a. Adjust mechanical zero with instrument turned off.
b. Turn instrument on and allow several minutes for voltages to stabilize.
c. Place a short circuit jumper wire between emitter and collector of the test transistor socket.
d. Set controls as follows:
   - Function switch in NOISE position
   - V. ADJ. full counterclockwise
   - Current range switch to 30
   - I. ADJ. full counterclockwise
e. Depress test transistor interlock switch.
f. Adjust screw driver adjustment R507 (located below and to the right of the *VOLTAGE* meter) for approximately zero indication of the *CURRENT* meter.
g. Remove short circuit and connect a DC voltmeter between emitter and collector of the test transistor socket.
h. Depress interlock switch and set V. ADJ. control to obtain 1 Volt.
i. Adjust R508 on assembly 1865 for a VOLTAGE meter indication of 1 Volt with the FULL SCALE VOLTS switch set to 1.
j. Repeat for R509 through R511 for voltage ranges 3 through 30.

4 KC Oscillator

a. Insert a phone plug partly into the β CAL. jack (located in rear of the instrument), only far enough to make contact, but DO NOT break the normally closed contact of this jack.
b. Measure the voltage at this point and adjust R607 on assembly 1872 to obtain 5.1 millivolts RMS.
c. Measure the frequency of this signal and adjust C603 assembly 1872 until frequency is 4.00 KC.

Compressor Filter

a. Insert a transistor in the test jig.
b. Apply normal operating voltage and current.
c. Set function switch to NOISE position.
d. Connect a high impedance DC voltmeter (approx. 4V) between either terminal of the Beta meter (ass'y 1865) and ground. (Beta meter is negative polarity respect to ground.)
e. Tune compressor filter C907 (ass'y 1872) for a maximum voltmeter indication.

Base Input Tank Circuit Adjustment

a. Insert a transistor in the test jig.
b. Apply normal operating voltage and current.
c. Set function switch to "β" position.
d. Connect a high-impedance DC voltmeter between either terminal of the Beta meter (assembly 1865) and ground.
e. Tune base input tank circuit (C509, ass'y 1864) for minimum voltmeter indication.

Beta Meter Calibration

a. Set controls as follows:
   - Function switch in "β" position
   - I. ADJ. full counterclockwise
   - V. ADJ. full counterclockwise
b. Insert a short circuit jumper between base and collector of the test transistor socket.
c. Close interlock switch.
d. Insert a plug in the β CAL. jack completely (to break the circuit of the internal 4 KC oscillator).
e. Apply a 510 millivolt 4.00 KC signal to the β CAL. jack.
f. Adjust R1009 (ass'y 1878) for a Beta meter indication of 100.

AGC METER CAL - SEE ERRATA SHEET #6

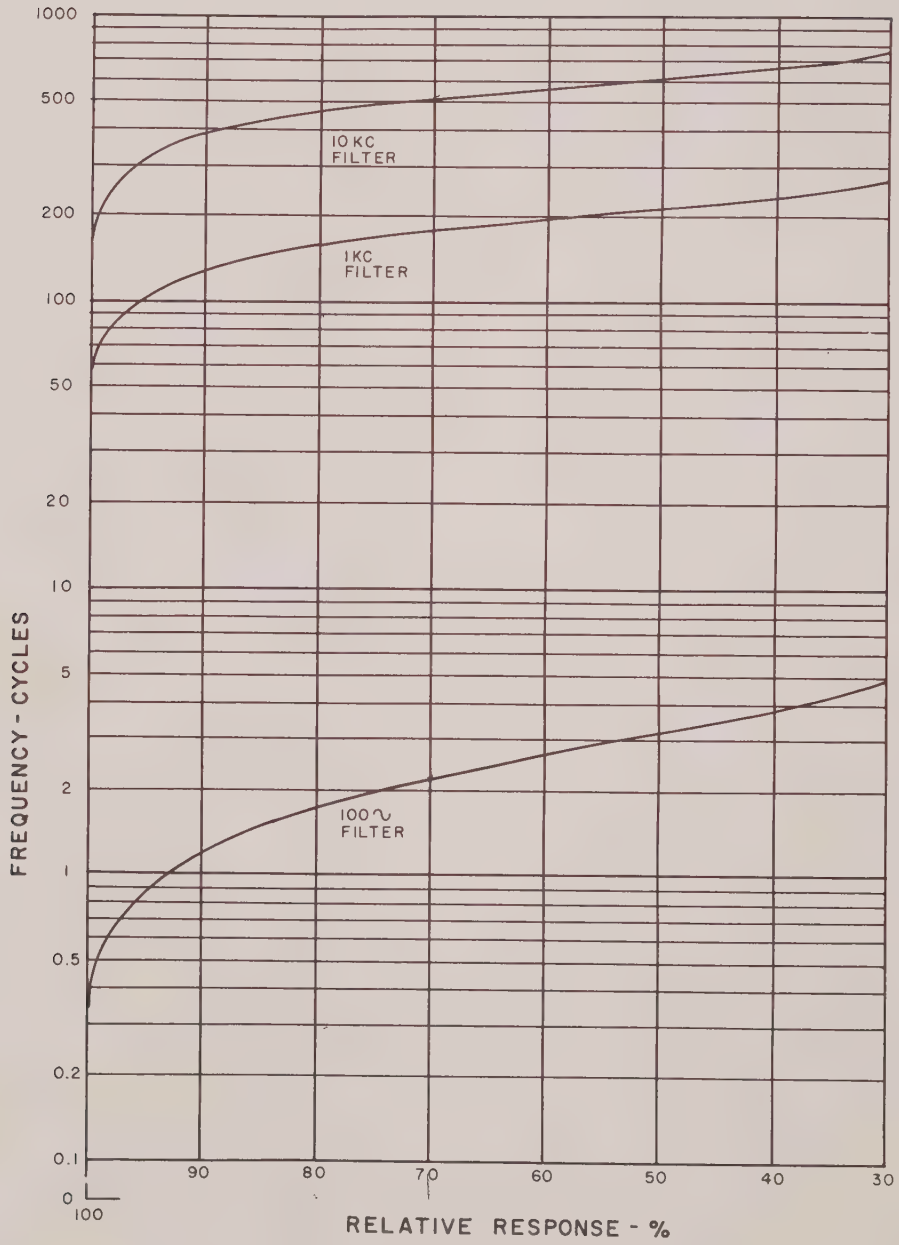


FIGURE 6-3. TYPICAL FILTER HALF BANDWIDTHS

Noise Meter Calibration

Each noise filter and amplifier must be calibrated separately, which involves the noise bandwidth of each filter, meter correction for noise signals and an attenuator constant. The attenuator constants have been computed and calibrating voltages for each filter are listed below. Typical bandwidth curves are shown in Fig. 6-3.

To calibrate, proceed as follows: (SEE ERRATA SHEET)

a. Connect an audio oscillator to the NOISE CAL jack (J502), inserting the phone plug completely.

b. Tune oscillator to the filter frequency.

c. Adjust oscillator level to the value for the filter concerned.

100 cycle = 2.46 mv (1.41)
1 KC = 16.9 mv
10 KC = 28.2 mv
100 KC = ... mv

d. Adjust NOISE CAL. screw driver adjustment in rear, behind the filter concerned to obtain full scale meter indication with the FULL SCALE meter switch in the 1 position.

e. With the calibrating signal still applied measure the DC voltage at the NOISE ANALOG jack for the filter concerned and adjust the screw driver adjustment (located on the printed-circuit board at the rear of the noise meter concerned) for 1 Volt DC for full scale indication.

f. Repeat the above procedure for the other noise-filter channels using the calibrating signal levels listed for each channel.

NOTE: When making the above adjustments, a high frequency transistor with an Alpha cutoff frequency of several megacycles should be used in the test jig, and the base selector switch should be in the E_N position to prevent errors at the higher frequencies due to transistor input capacitance.

NOT PART OF NORMAL CAL PROCEDURE

THRESHOLD NOISE MEASUREMENT

With the known amplification factor method of calibration utilized in the Model 310, internal amplifier gain is highest when the test transistor gain is lowest. This condition occurs at low collector current when the FUNCTION switch is in the NOISE position.

Amplifier system noise is completely masked by the thermal noise from the 10,000 ohm base resistor when measuring I_N. (Correction for the 10K thermal noise is described on page 3-0 under OPERATIONAL HINTS.) Amplifier system noise may become an important factor when measuring E_N on a very quiet transistor at very low collector current. Typically E_N readings can be taken directly with less than 1db error due to system noise down to collector currents of approximately 50 microamperes on the 10KC filter, 100 microamperes on the 1KC filter and 200 microamperes on the 100 cycle filter.

A method of determining system noise follows so that E_N readings may be corrected if required in the very low collector current area.

The measured noise voltage (E_N) is corrected through the use of the following equation:

$$\text{Corrected } E_N = (\text{measured } E_N^2 - \text{system } E^2)^{1/2}$$

In general, system noise will vary approximately inversely with collector current and will be different for each of the three frequencies monitored at a fixed collector current.

The procedure for measuring system noise for a particular DC collector current is as follows:

a) Set Model 310 front panel FUNCTION switch to NOISE, I. ADJ. full counterclockwise and V. ADJ. full counterclockwise.

b) Connect the ground sides of two external audio oscillators to the grounding braid between the test jig cover and base plate of the Model 310. Connect the high sides of both oscillators through separate 1 megohm resistors to the collector pin of the test socket.

c) Tune one oscillator to 1KC and set its output voltage to the magnitude given by the following equation:

$$\text{1KC osc. voltage} = \left(\frac{I_C}{.025}\right)\left(\frac{\text{1KC cal. voltage}}{A}\right)\left(10^6\right) \text{ volts}$$

WHERE:

I_C = the particular DC collector current in amperes at which system noise is to be measured.

1KC cal. voltage = 1KC cal voltage given on page 6-5 of the instruction manual.

A = 1040

d) Tune second oscillator to 4KC and close test jig interlock switch.

e) Increase output voltage of 4KC oscillator until 1 KC NOISE meter reading comes down to approximately full scale on the 1 position of the FULL SCALE range switch.

f) Fine tune 4KC oscillator frequency for *minimum* reading on IKC NOISE meter.

g) Adjust 4KC output voltage for precisely full scale reading on IKC NOISE meter.

h) Remove IKC oscillator and series resistor and read system noise (at I_C used in above equation) on each of the NOISE meters.

NOTE: System noise at particular values of I_C are meaningful only when the transistor to be tested has the following qualifications: Beta greater than 10 and I_C much greater than I_{CBO}.

System noise measured as directed above is a noise voltage referred to the base of the transistor under test. An equivalent noise current in the collector of the transistor under test can be obtained through the use of the transconductance equations:

$$\Delta i_c = gm\ (\Delta e_b) \qquad gm = \frac{I_C}{.025}$$

WHERE:

Δi_c = equivalent collector noise current.

Δe_b = measured system noise voltage referred to the base of the transistor under test.

I_C = the particular DC collector current in amperes at which system noise was measured.

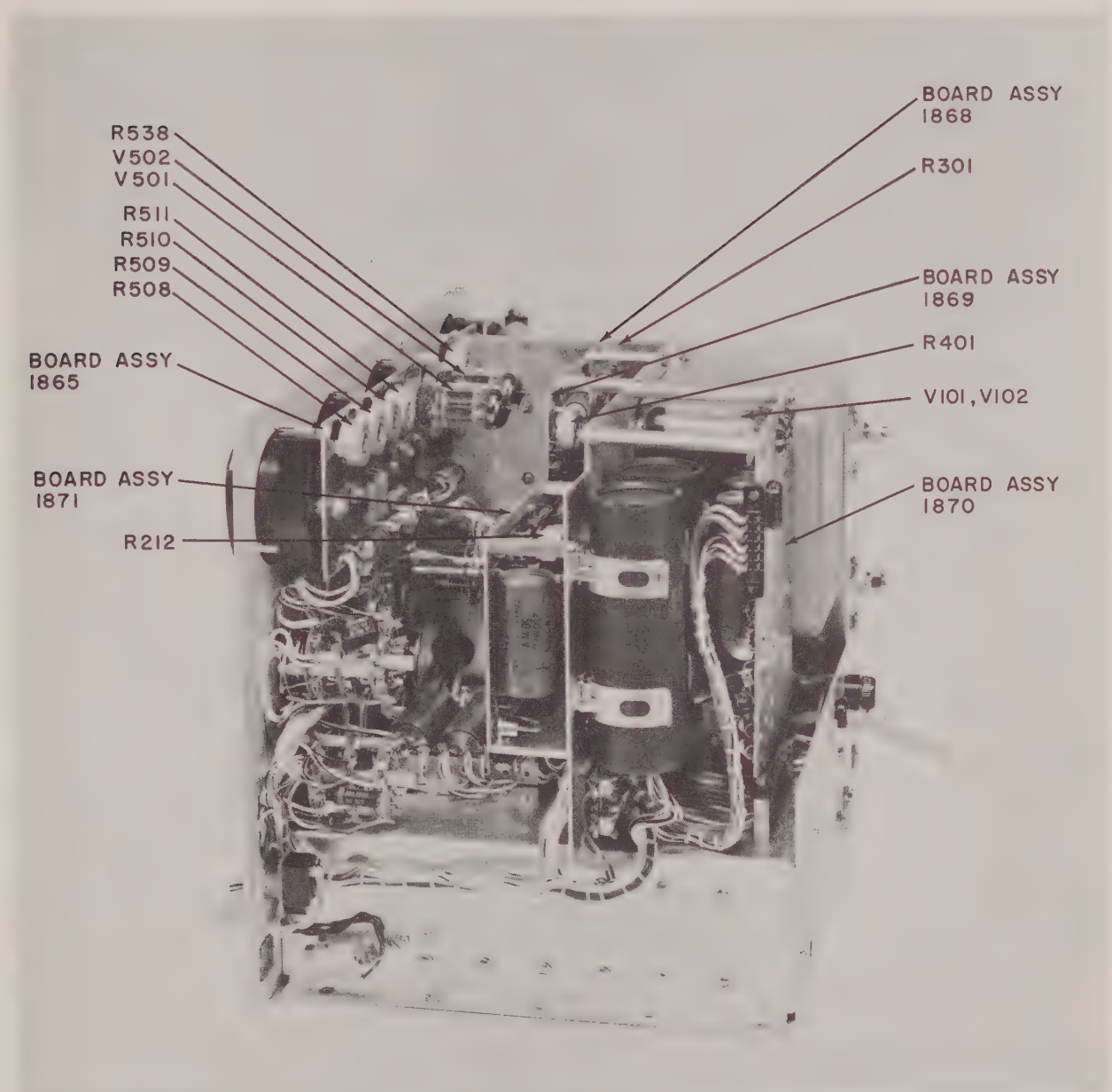


FIGURE 6-4. INTERNAL VIEW FROM RIGHT SIDE

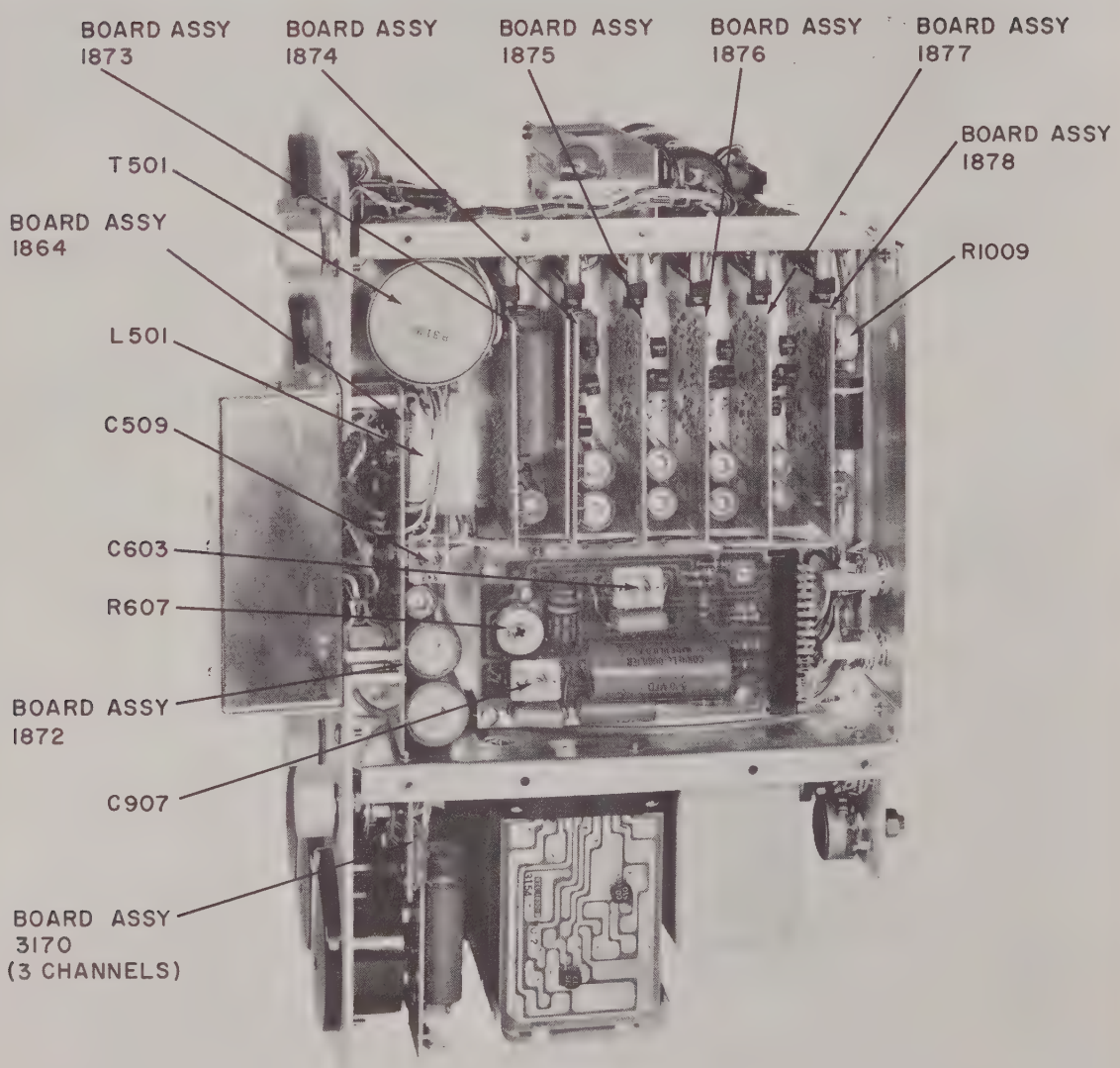


FIGURE 6-5. INTERNAL VIEW FROM BELOW

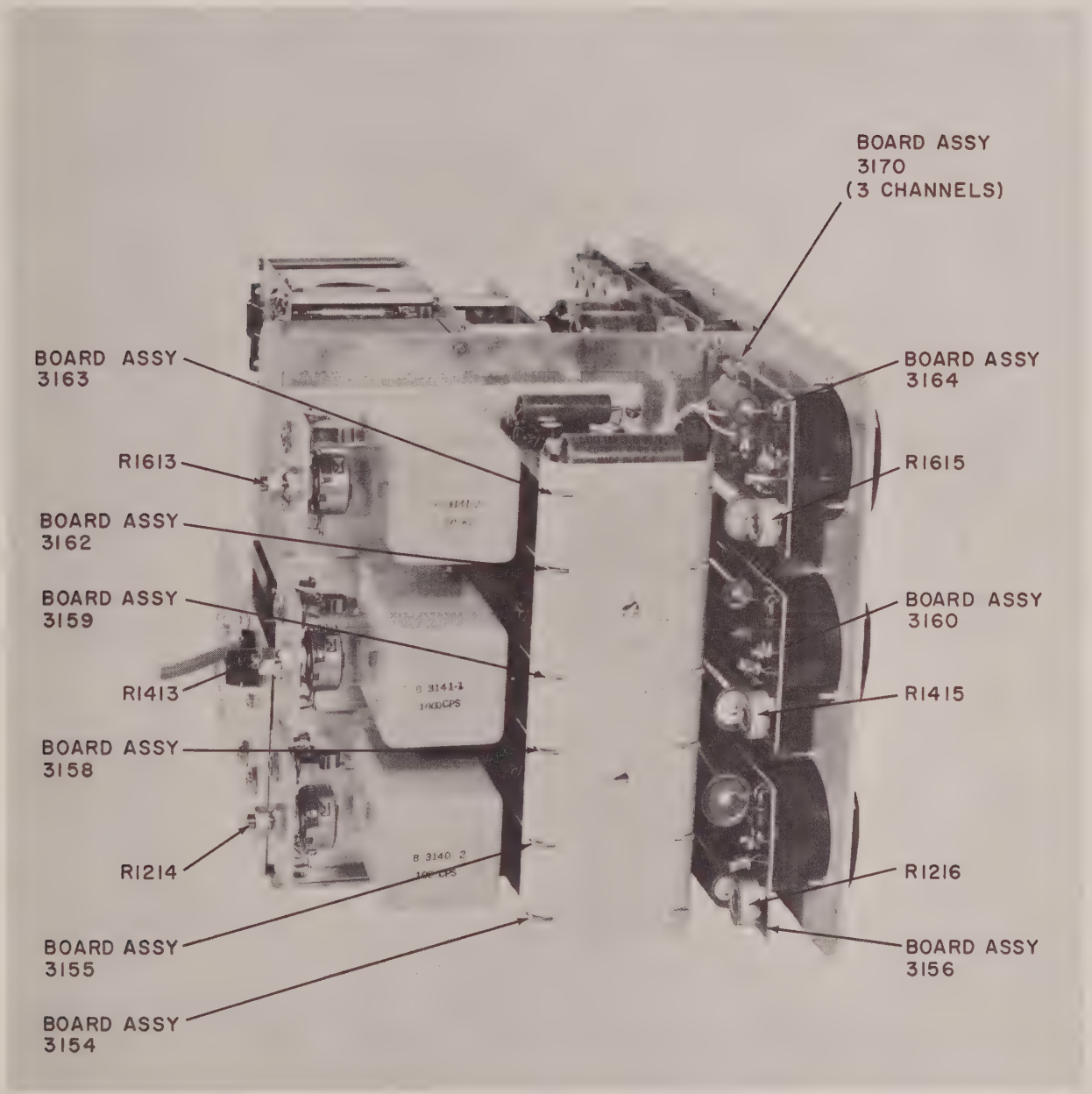


FIGURE 6-6. INTERNAL VIEW FROM ABOVE

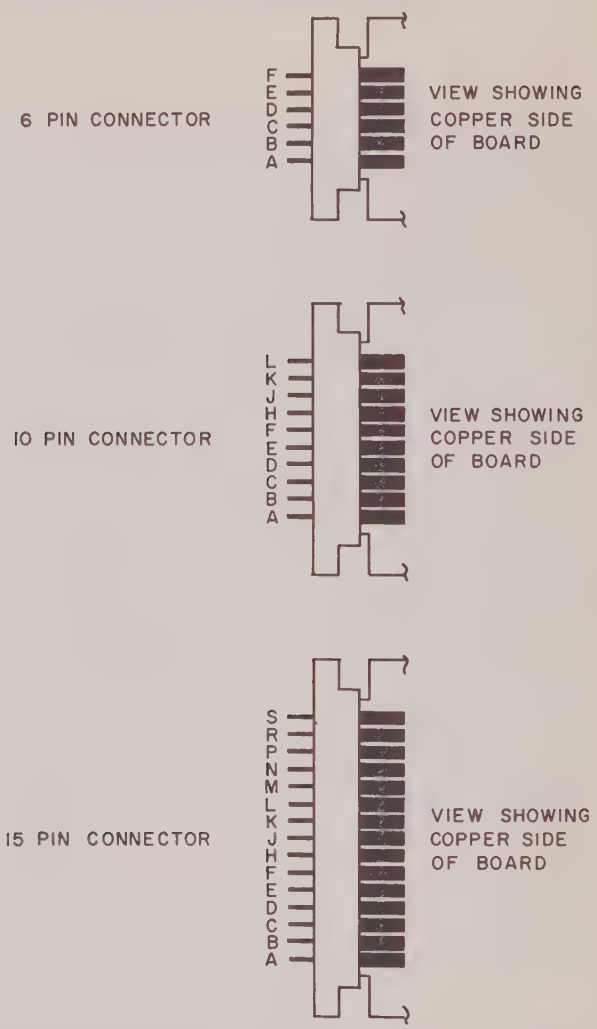

6 PIN CONNECTOR
F E D C B A
VIEW SHOWING COPPER SIDE OF BOARD
10 PIN CONNECTOR
L K J H F E D C B A
VIEW SHOWING COPPER SIDE OF BOARD
15 PIN CONNECTOR
S R P N M L K J H F E D C B A
VIEW SHOWING COPPER SIDE OF BOARD

FIGURE 6-7. PRINTED CIRCUIT BOARD CONNECTOR LUG IDENTIFICATION

SCHEMATIC LEGEND

K = 1000

⊘ = Screw Driver Adjustment

▭ = Front Panel Control

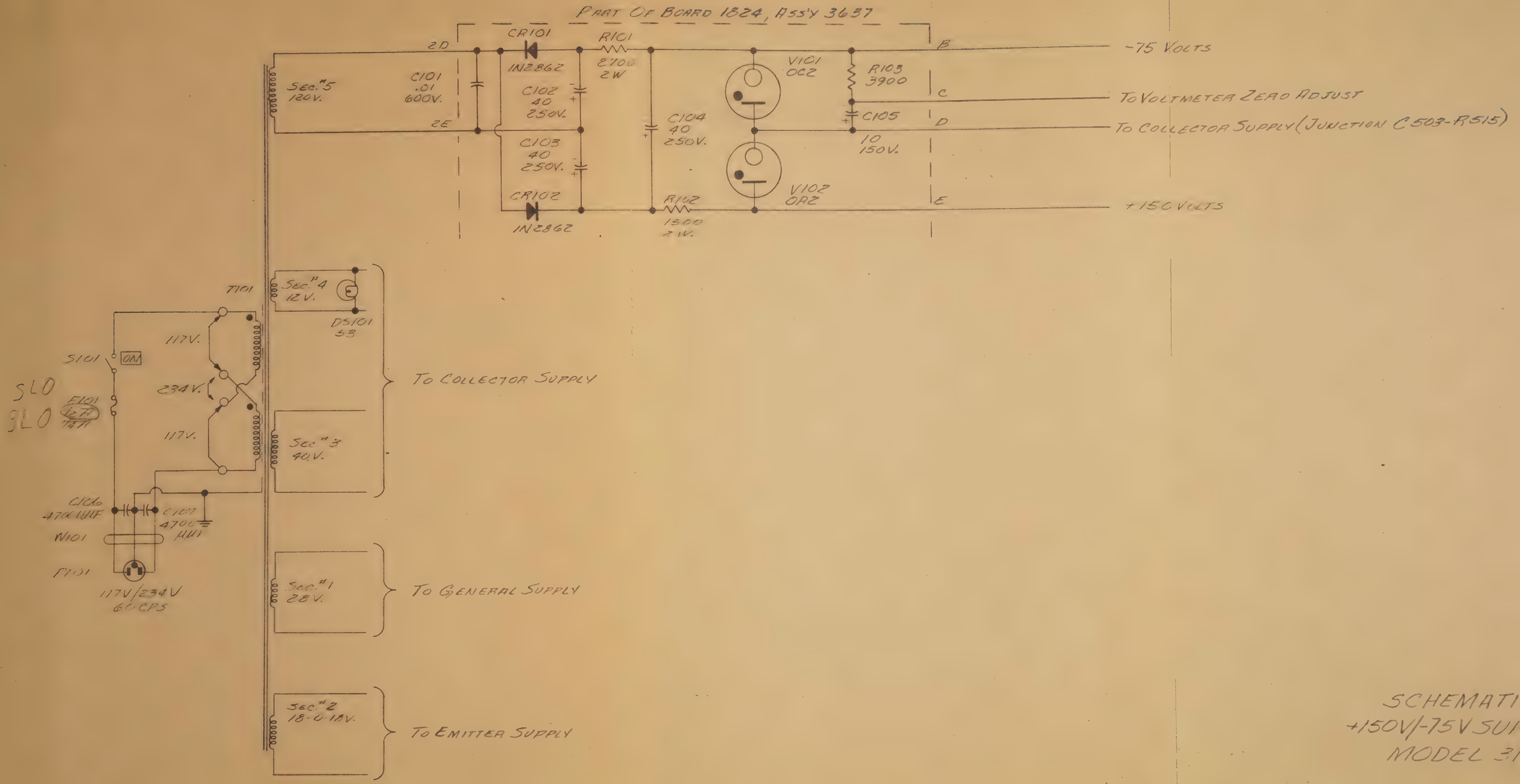
* = Factory Select

Unless Otherwise Specified:

All Resistances in Ohms

All Resistors ½ Watt

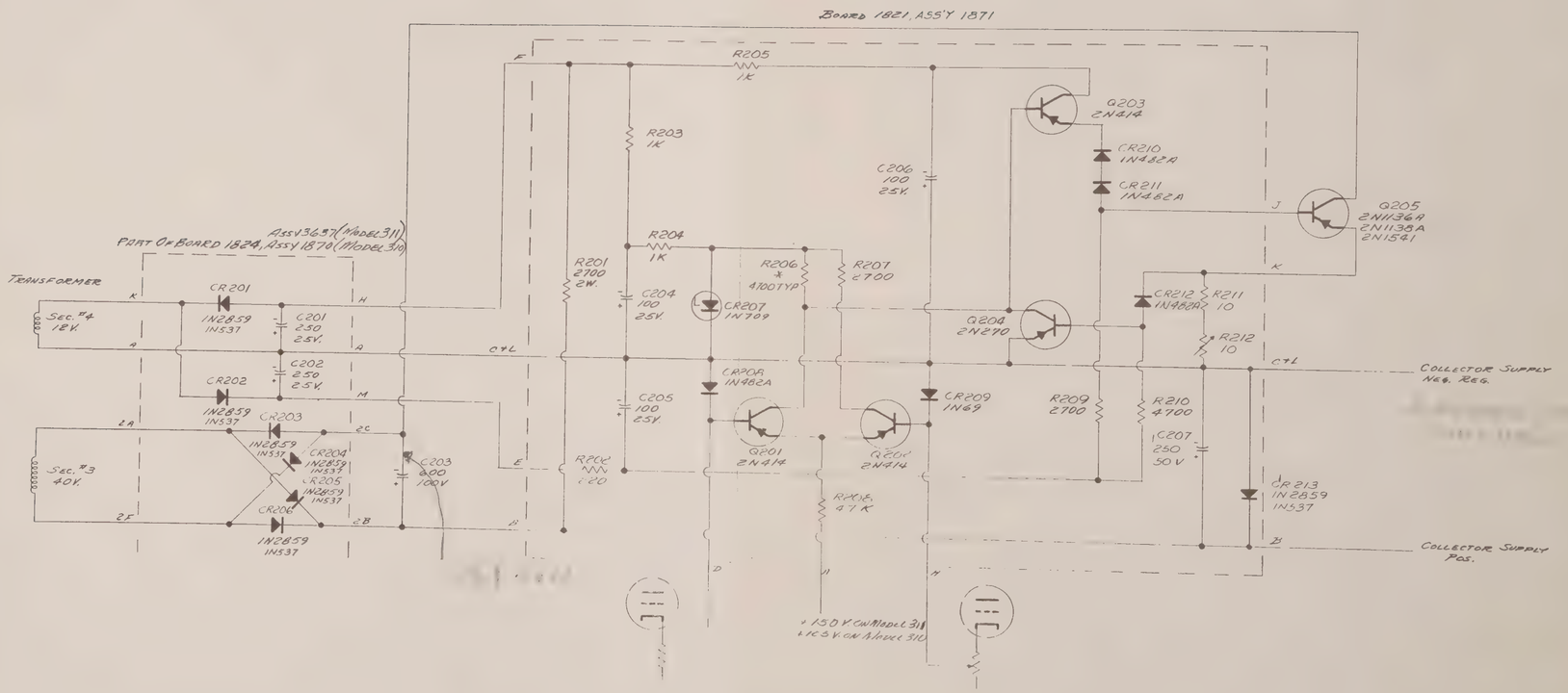
All Capacitances in Microfarads



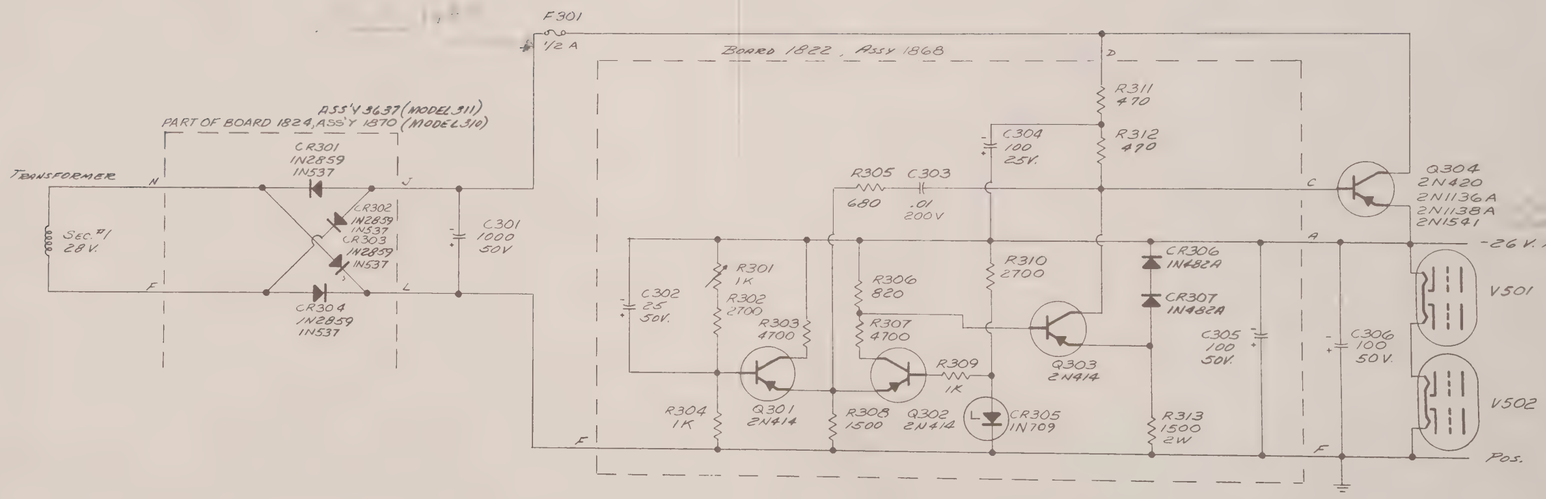
SLO
SLO

SCHEMATIC
+150V/-75V SUPPLY
MODEL 311

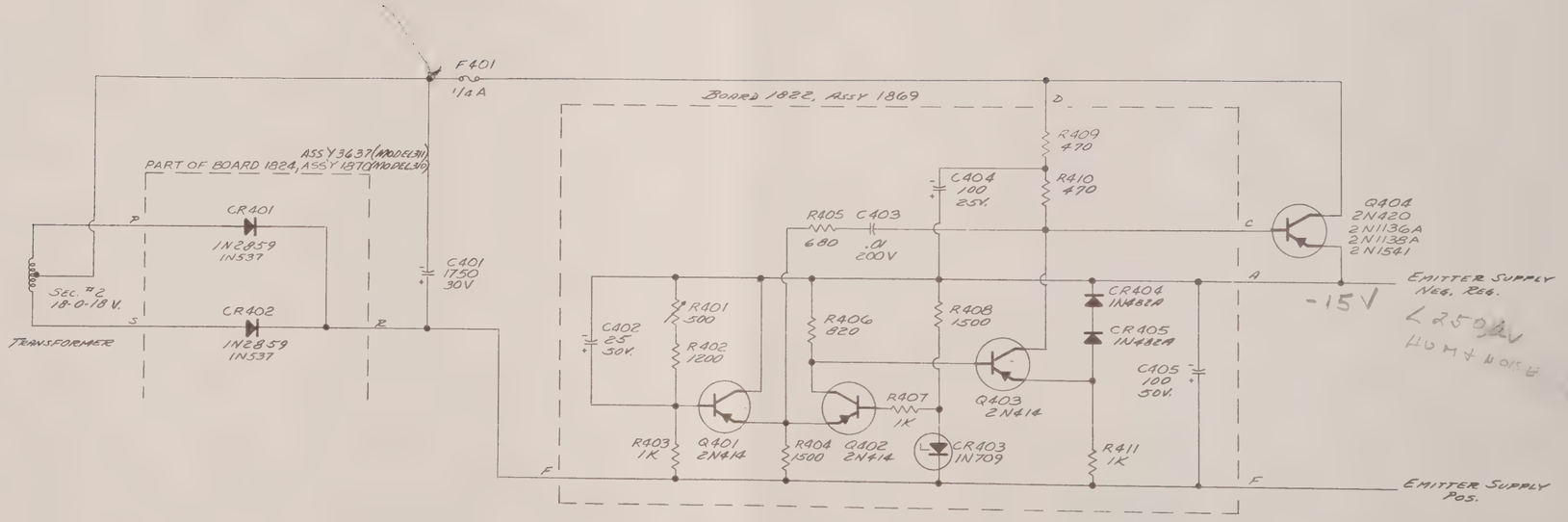
T-3636-A



SCHEMATIC
COLLECTOR SUPPLY
MODEL 310
(Drawing No. T-3102E)



SCHEMATIC
–26 VOLT SUPPLY
MODEL 310
(Drawing No. T-3103E)



SCHEMATIC
EMITTER SUPPLY
MODEL 310
(Drawing No. T-3104F)

COLLECTOR SUPPLY 0-30V

TO-75/+150V SUPPLY

S501A S501B S501C S501D S501E S501F S501H S501I S501J S501L S501M

NPN PNP

C502 250 50V

C509 .05 200V.

C507 .05 200V.

R518 316K
R519 1MEG
R520 3.16M
R521 10M
R522 31.6M

3 1 .3 .1 .03 μA

S503D

R523 1K
R524 3.16K
R525 10K
R526 31.6K
R527 100K

1000 300 100 30 10 μA

S503A

NOISE Icbo Iebo

S505A

PART OF BOARD 1827 ASS'Y 3606

+150V

V502 12AU7A

R537 1K
R538 2500
M502
R536 47K
R540 47K
CURRENT

R539 10K ZERO ADJUST

-75V

R535 10K

-26V REG

TO AGC METER

S505B

T501

PC GN

TO AMPL #1

PART OF BOARD 1827 ASS'Y 3606

+150V

1/2 V501 12AU7A

R502 2210
R508 1K
R503 11K
R509 2500
R504
R510 5K
R505 41,200
R506 147K
R511 5K
R512 10K
R513 9K
R501 18K
R507 10K ZERO ADJUST

.1 3 10 30

S502

M501

VOLTS VOLTAGE

V ADJ

TYP

TO -75V SUPPLY (PIN C)

S504A (IN TEST POS.)

S504B (IN TEST POS.)

S503B

R528 10K
R529 33K
R530 100K
R531 330K
R532 1M

R534

S505C S505D S505E

TRANSISTOR UNDER TEST (NPN SHOWN)

C508 4700μμF

EMITTER SUPPLY 15V

R514 22

C501 1000 15V

PART OF BOARD 1826, ASS'Y 3605

R517 4.7

C504 250 25V
C505 25 50V
C506 5 50V

S503C

PART OF BOARD 1826 ASS'Y 3605

R541 499
R542 11K

500 1K

S506

P547 1K

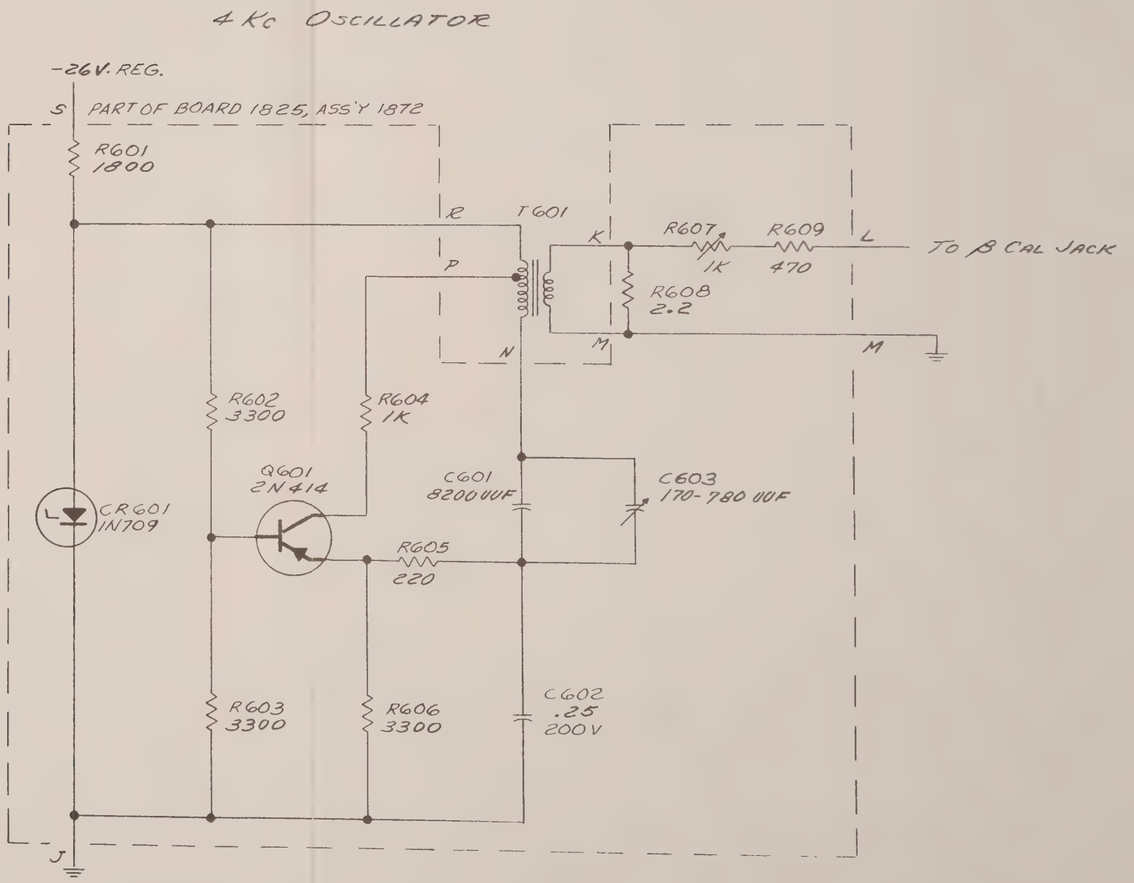
J501 BCAL

TO 4KC OSC

J502 NOISE CAL

SCHEMATIC
FRONT PANEL SWITCHING
MODEL 311

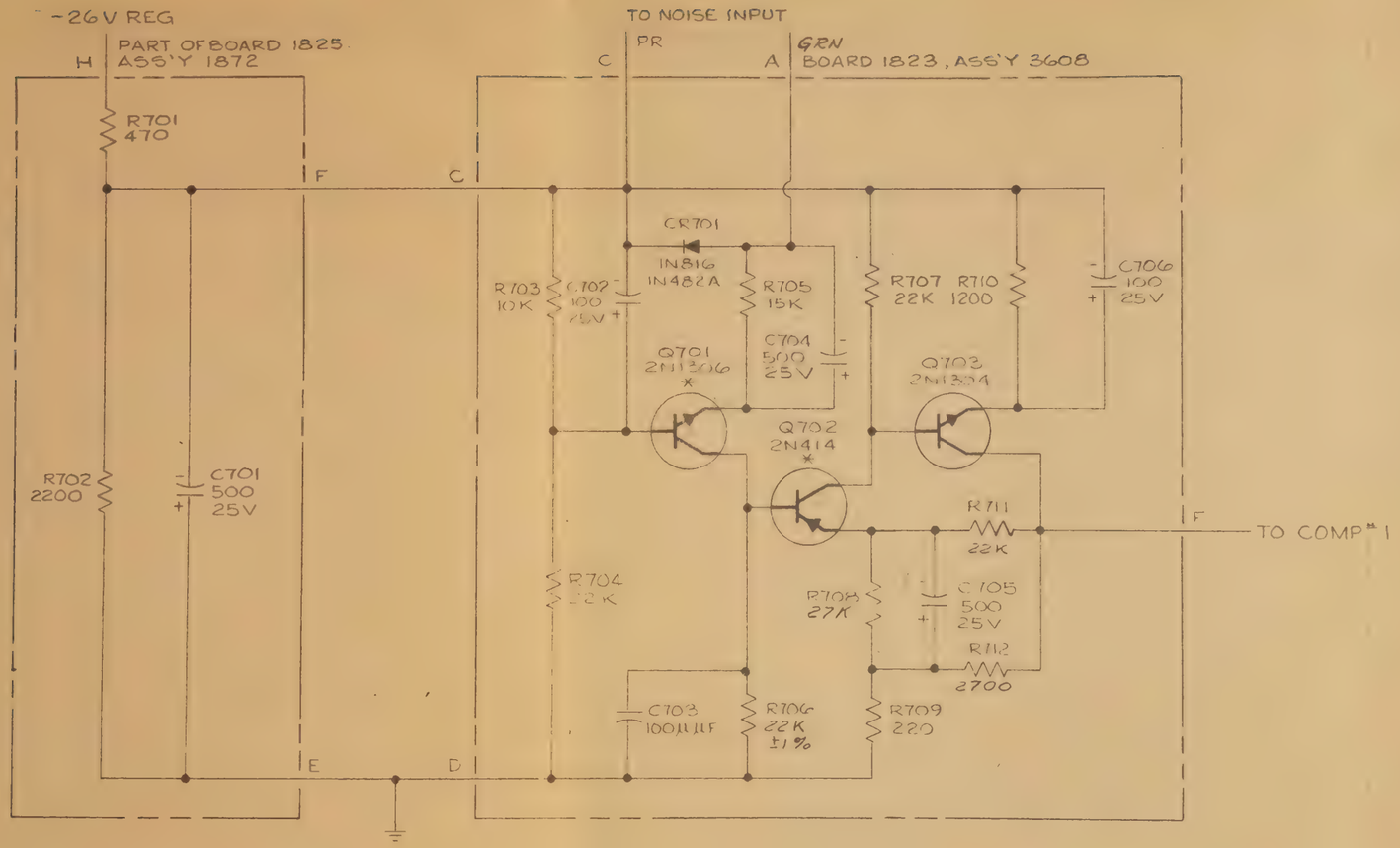
C-3601 C



SCHEMATIC
4 KC OSCILLATOR
MODEL 310
(Drawing No. T-3106C)

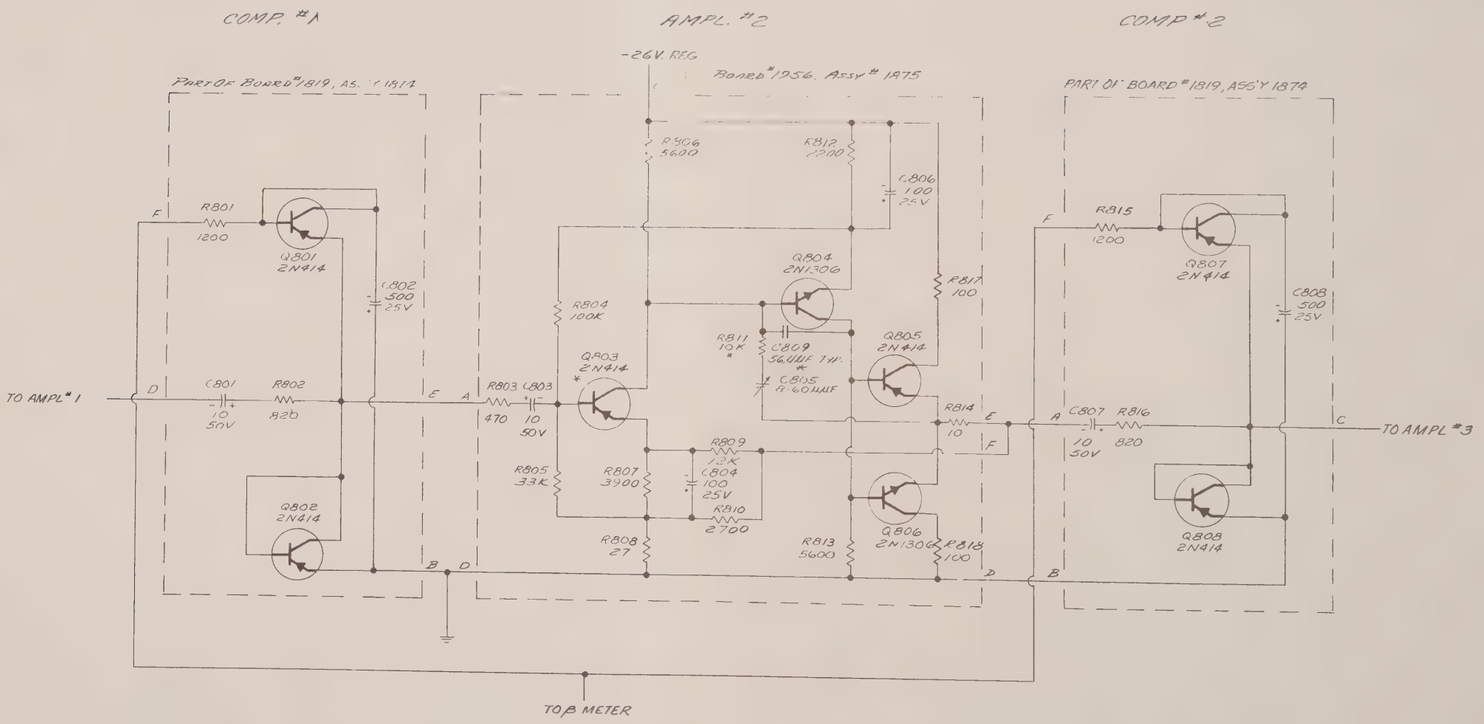
DC FILTER

AMPL #1

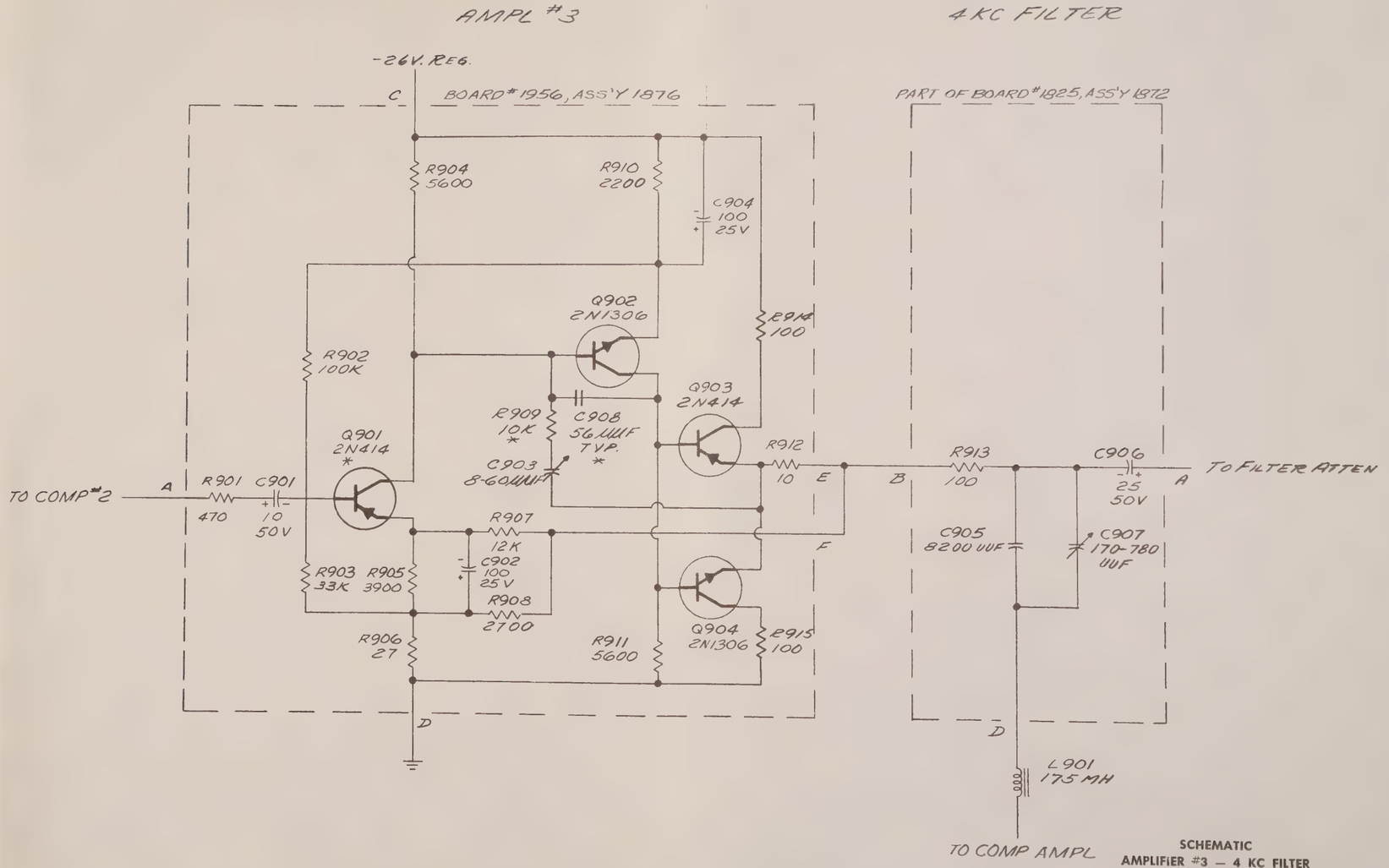


SCHEMATIC
AMPLIFIER #1 & FILTER
MODEL 311

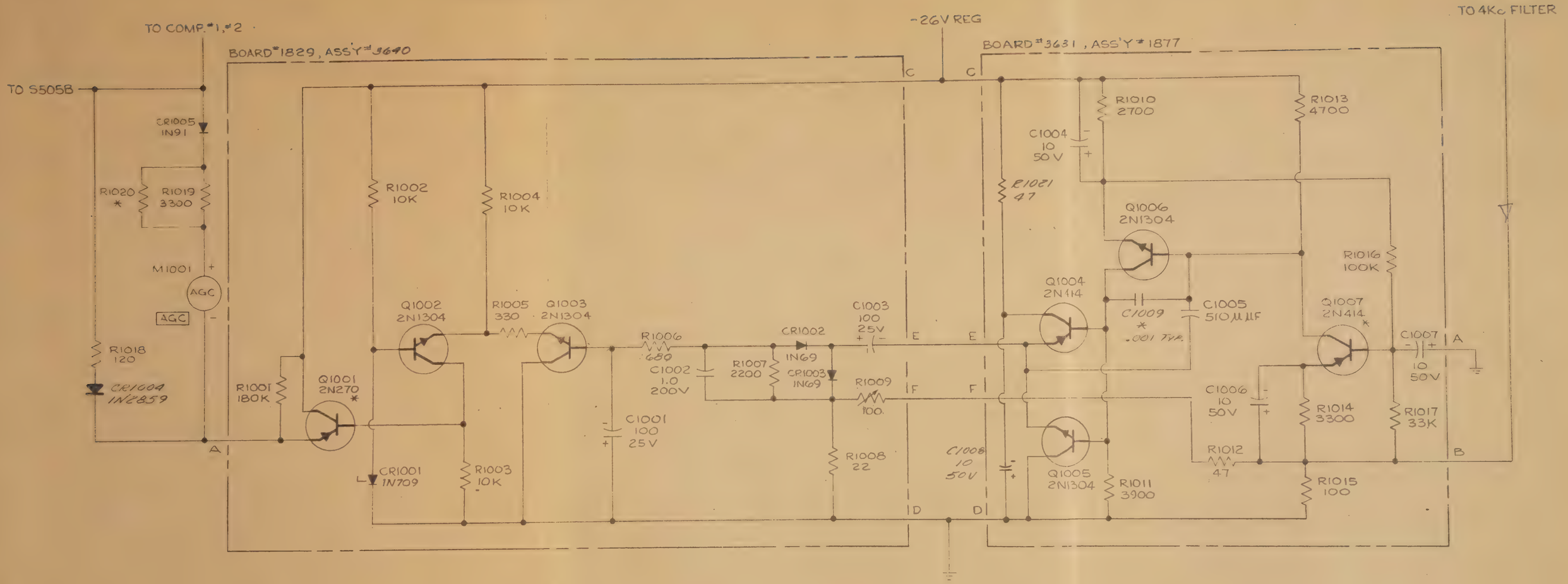
T-3602 B



SCHEMATIC
COMPRESSOR #1 — AMPLIFIER #2 — COMPRESSOR #2
MODEL 310
(Drawing No. T-3108D)

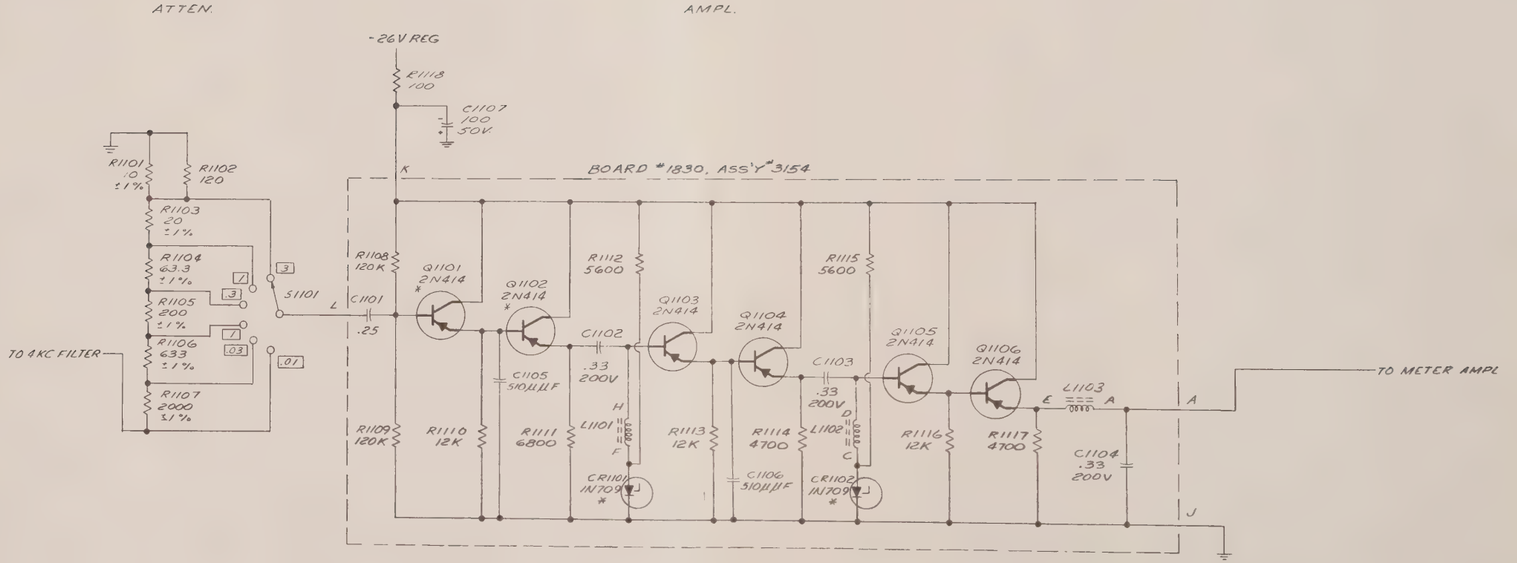


SCHEMATIC
AMPLIFIER #3 — 4 KC FILTER
MODEL 310
(Drawing No. T-3109D)

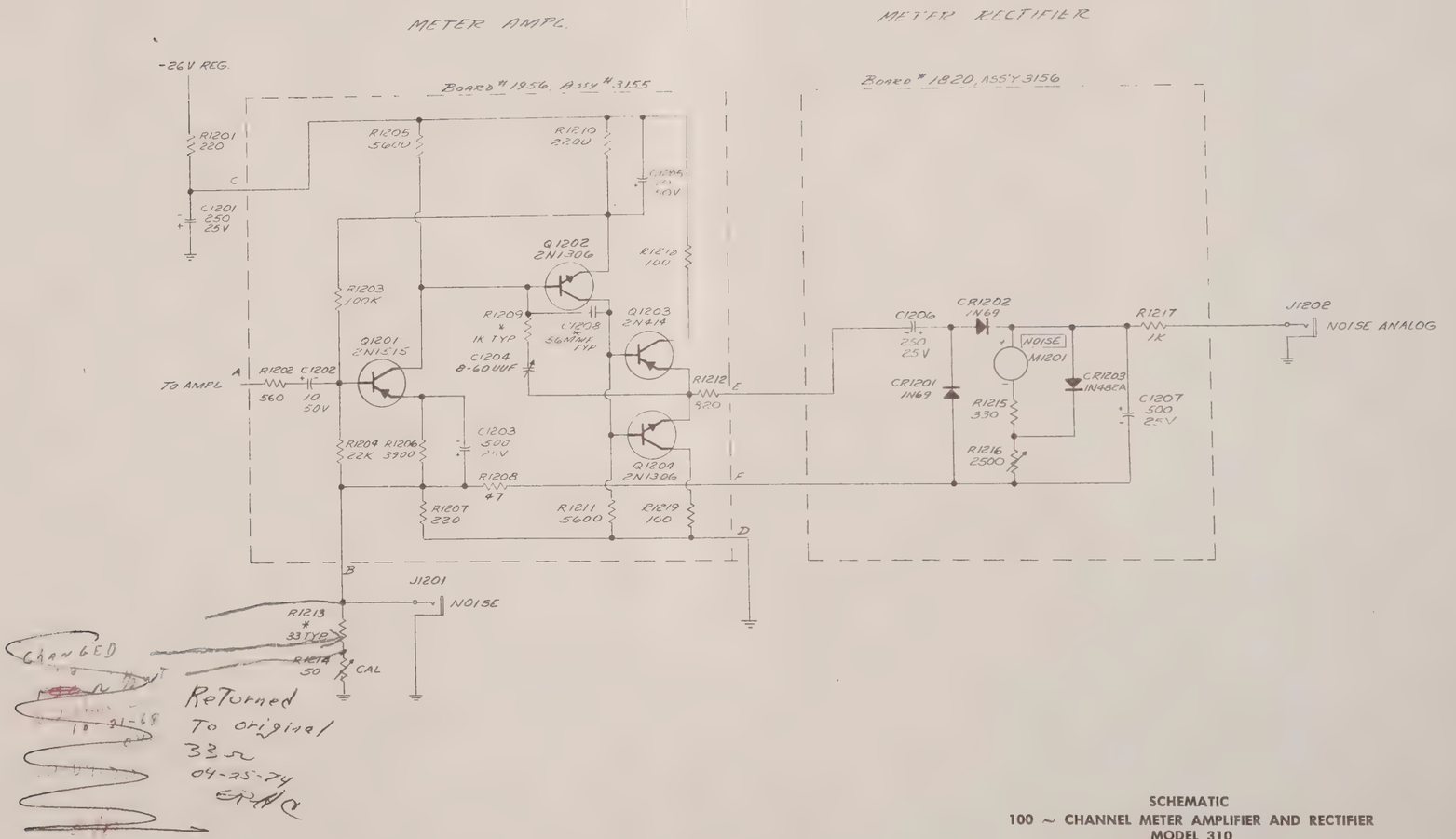


SCHEMATIC
COMPRESSOR AMPLIFIER-
COMPRESSOR DRIVER
MODEL 311

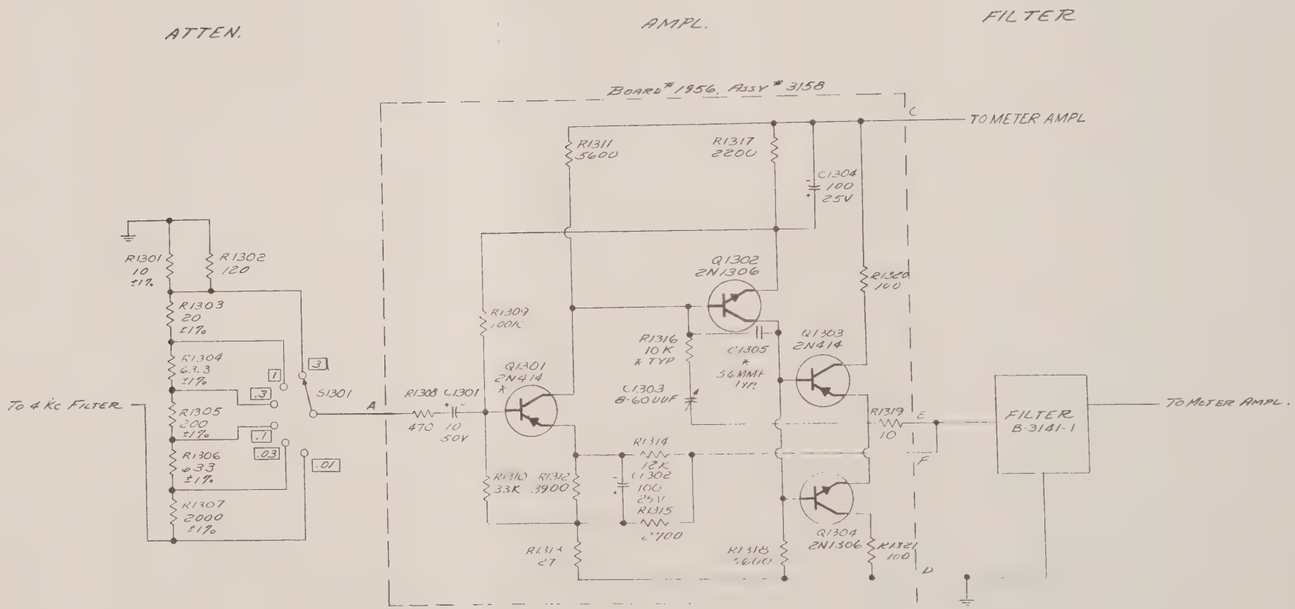
T-3603 D



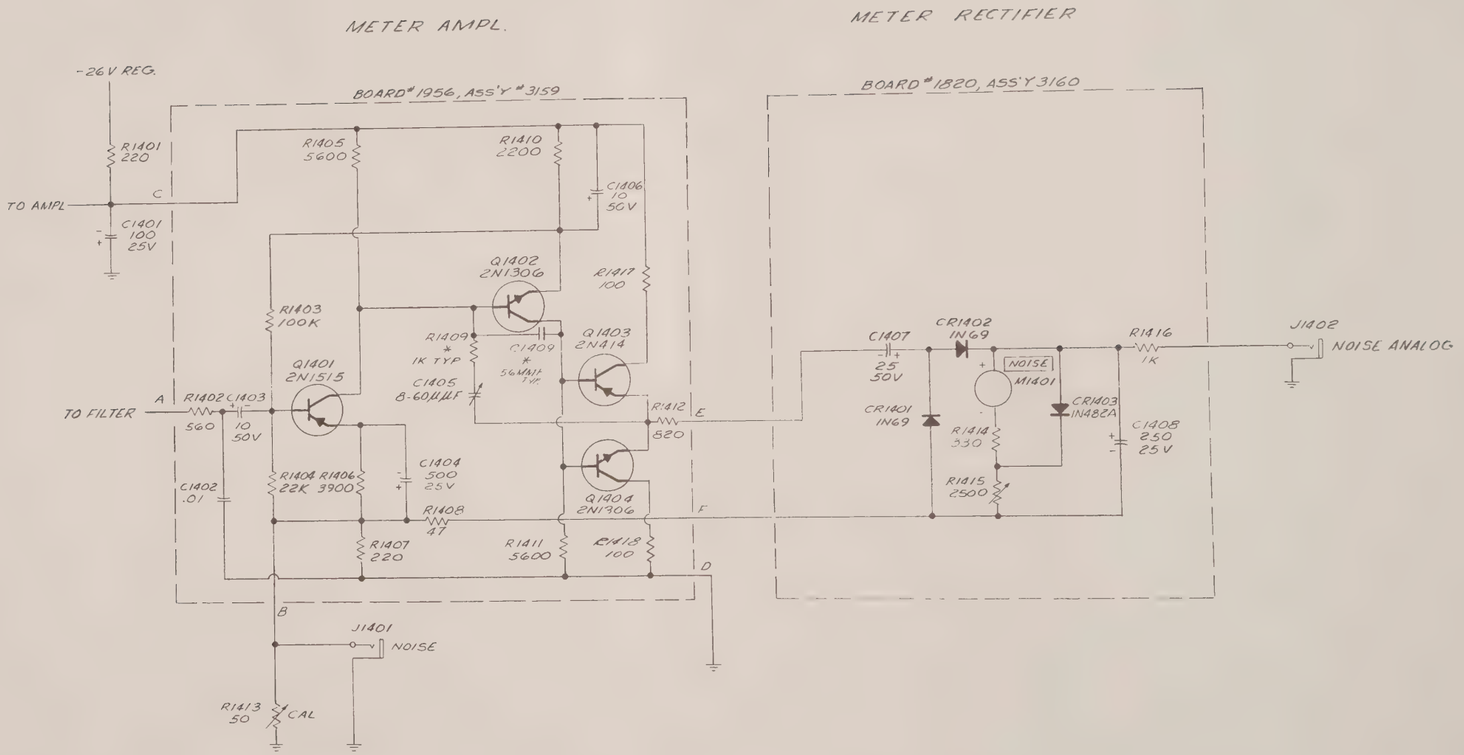
SCHEMATIC
100 ~ CHANNEL AMPLIFIER AND FILTER
MODEL 310
(Drawing No. T-3111D)



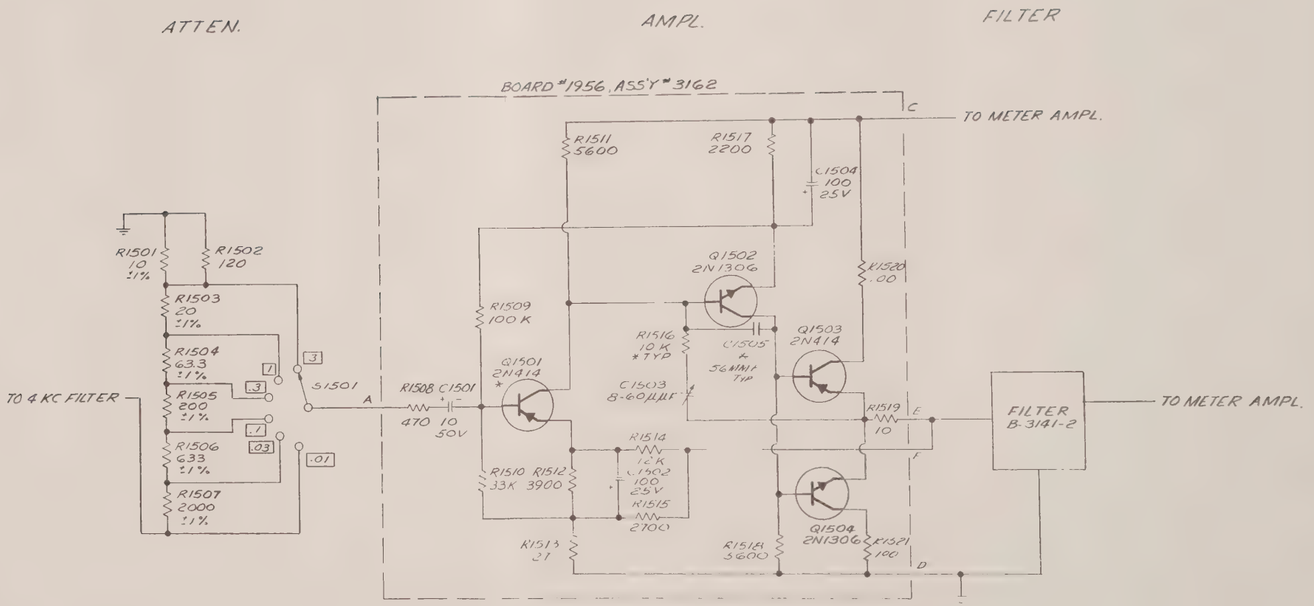
SCHEMATIC
100 ~ CHANNEL METER AMPLIFIER AND RECTIFIER
MODEL 310
(Drawing No. T-3112E)



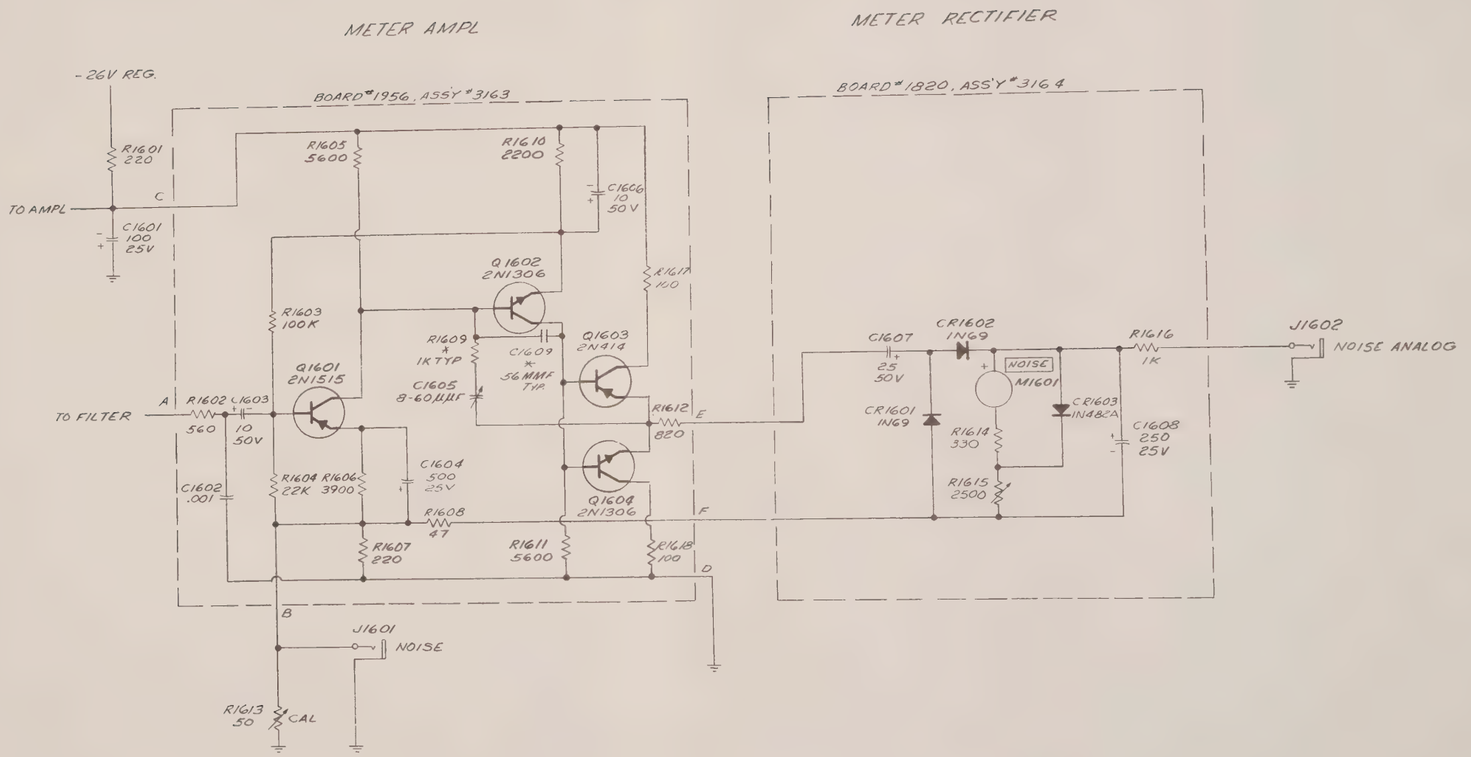
SCHEMATIC
1 KC CHANNEL AMPLIFIER AND FILTER
MODEL 310
(Drawing No. T-3113C)



SCHEMATIC
1 KC CHANNEL METER AMPLIFIER AND RECTIFIER
MODEL 310
(Drawing No. T-3114D)



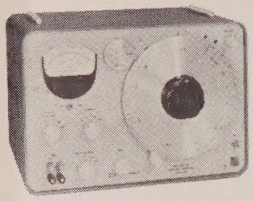
SCHEMATIC
10 KC CHANNEL AMPLIFIER AND FILTER
MODEL 310
(Drawing No. T-3115C)



SCHEMATIC
10 KC CHANNEL METER AMPLIFIER AND RECTIFIER
MODEL 310
(Drawing No. T-3116D)

Mr. Stone

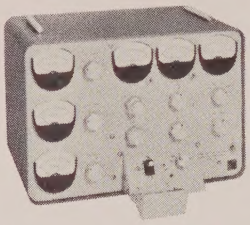
Quan-Tech INSTRUMENTS



MODEL 303
WAVE AND NOISE SPECTRUM ANALYZER

Fully transistorized spectrum analyzer covers frequency range from 30 cps to 100 kc. Front-panel selection of 4 constant bandwidths (10, 30, 100 & 1000 cps) the 100 & 1000 cps bandwidths are flat topped, simplifying noise computations, greatly improving accuracy, and simplifying tuning. Sensitivity: 100 μv to 300 v, full scale; down to 1 μv full scale with Model 203 Amplifier (see below). Additional features: ± 300 cps vernier; selection of long or short meter time constants; metering circuits compensated to minimize error from instantaneous noise pulses; overload protected meter; analog output for external monitoring.

PRICE: ~~$1425~~ $1475



MODEL 310
TRANSISTOR NOISE ANALYZER

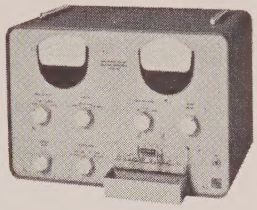
Measures noise at 100 cps, 1 kc and 10 kc simultaneously for 3-point spectrum analysis, allowing identification of 1/f-portion of transistor noise. Measures noise voltage over range from 0.01 to 3 μv/root cycle FS, and noise current from 1 to 300 pa/root cycle, FS. Collector current range, 0.05 to 30 ma; collector voltage range, 0.1 to 30 v. Measuring system automatically corrects for variations in transistor gain; measurement also provided of beta, I_{cbo} and I_{ebo}.

PRICE: ~~$2075~~ $2375

MODEL 311 TRANSISTOR NOISE ANALYZER

Similar to above, except that collector current range extends from 5 to 1000 μamperes, for measurement of noise in low-collector-current devices. Beta measurement is not available in the Model 311.

PRICE: ~~$2275~~ $2575



MODEL 315
RESISTOR NOISE TEST SET

Measures noise in resistors in conformance with specifications recommended by National Bureau of Standards and Method 308 of MIL STD 202 B. Tests resistors from 100 ohms to 22 megohms. Range of measurement: 0.6 μv in a decade to 1000 μv in a decade. Output of noise voltage for external monitoring; analog outputs of meter readings for data logging, etc. External cable included to permit locating test jig up to 10-feet from instrument.

PRICE: ~~$1700~~ $1950

MODEL 2136

Same specifications as Model 315 except measures resistors down to 10 ohms.

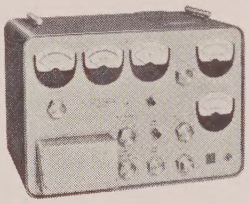
PRICE: $2300

MODEL 317
AMPLITUDE DISTRIBUTION ANALYZER

Establishes the amplitude-probability distribution of random signals to determine whether distribution is Gaussian, or to establish threshold requirements, false-alarm probabilities, etc. Amplifier response: 3db down at approx. 12 cps and 1 mc. Switching rate: 5 mc. Amplitude ranges: 100%, 10% and 1%, FS. "inverted" operation, indicating what percentage of time preset limit is not exceeded, also provided. Output to drive counter at front panel; voltage level may be swept from external source (such as oscilloscope sweep output) for automatic display.

PRICE: ~~$385~~ $450

MODEL 327
DIODE NOISE ANALYZER



Measures noise in back-biased semi-conductor diodes over range of 0.03 μv to 1 mv per cycle of bandwidth at 10 cps and 1 kc simultaneously. Diode test voltage adjustable up to 500 v; current, to 100 ma. Internally generated ramp sweeps test voltage and/or current automatically within maximum ratings. Sweep selectable in 3 speeds. A wide variety of signal and analog outputs for data logging, external monitoring, actuating external equipment, etc.

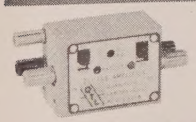
PRICE: ~~$2450~~ $2750

MODEL 420 RANDOM NOISE GENERATOR

Provides stable "white" noise output that is gaussian in amplitude distribution from DC to 100 KC. Calibrated output is continuously variable from 0.01 to 1000 μv per root cycle. DC offset is less than 10 mv at max. output. Completely solid-state instrument measures 12" x 6" x 8".

PRICE: $525

SOLID STATE AMPLIFIERS



MODEL 201-B
DC-COUPLED DECADE AMPLIFIER

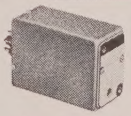
Provides controlled gain of 10 from DC to 3 mc (3db). Completely self-contained; battery operated; built-in battery-condition indicator.

PRICE: ~~$95~~ $110

MODEL 203
LOW NOISE AC AMPLIFIER

Controlled gain of 100 from 30 cps to 100 kc (±0.5 db), down 3 db at 500 kc. Typical noise: 5 x 10^{-9}V and 3 x 10^{-13}A per root cycle at 1 kc. Two Mod. 203's may be plugged together in series for gain of 10,000. Battery operated; fully self-contained; built-in battery condition indicator.

PRICE: $125



MODEL 205
HIGH-STABILITY DC AMPLIFIER

Controlled gain of 10 from dc to 100 kc. Highly stable: typical shorted input drift less than 250 μv at room ambient. Octal basing for plug-in installation. External + and — 12 v. required.

PRICE: $105

All prices shown are F.O.B. Boonton, N. J. Prices and specifications subject to change without notice.

Quan-Tech LABORATORIES, INC.

~~68 PARSIPPANY BOULEVARD • BOONTON, N. J. • U.S.A. • PHONE (201) 334-8500~~

43 So. JEFFERSON RD.
WHIPPANY N.J.

MR. STOVER

201-887-5508

www.manualsplus.com
1035286